NOV 14 1963

INSTRUCTION MANUAL

MODEL 315

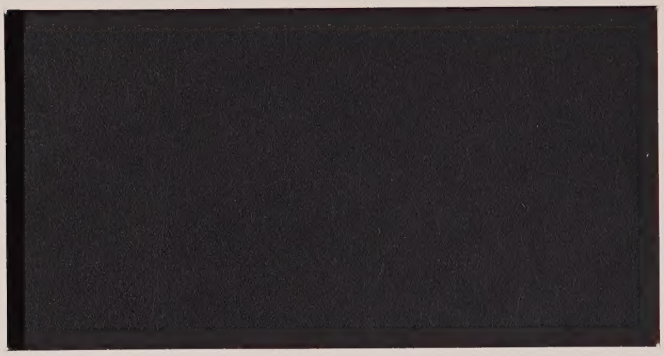
RESISTOR-NOISE TEST SET

For Serial No._____

BAC 520272

• ELECTRONIC INSTRUMENTS

Quan-Tech
LABORATORIES INC.
BOONTON, N. J.



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PHONE: DE 4-8500

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MODEL 315

RESISTOR-NOISE TEST SET

GENERAL

The Model 315 is a compact, bench-size instrument for making precise quantitative measurements of excess resistor-noise. The index of measurement is microvolts-per-volt in a decade of frequency, expressed in decibels as recommended by the National Bureau of Standards.*

SPECIFICATIONS

RANGE ..... Resistor Test Range — 100 ohms to 22 megohms.

Noise Voltage — 0.6 microvolts in a decade to 1000 microvolts in a decade.

Applied DC Voltage — 3 to 300 volts.

FILTER ..... Geometric mean 1000 cycles, flat-topped bandpass.

DETECTOR ..... Pure RMS.

OUTPUT ..... Indicated for both noise voltage and applied DC voltage on separate panel meters as well as analog outputs for data processing. AC monitor jack included.

ACCURACY OF NOISE VOLTAGE MEASUREMENT ..... ±5%.

DIMENSIONS ..... 15" W x 11" H x 11" D overall, weight 30 lbs., completely self-contained.

POWER INPUT ..... 117/234 volts, 50-60 cycles, 60 watts.

*See: "A Recommended Standard Resistor Noise Test System," G. T. Conrad, Jr., N. Newman, & A. P. Stansbury; I.R.E. Transaction of the Professional Group on Components Parts; Vol. CP-7, No. 3, Sept. 1960. Reprint available from Quan-Tech Laboratories on request.

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SECTION 1

OPERATING INSTRUCTIONS

RESISTOR MEASUREMENTS

1. For initial operation of the Resistor-Noise Test Set, plug the power cord into a suitable source of power. Refer to the plate on the rear of the instrument near the power cord for the voltage and frequency for which this instrument is wired. See Section 5 for instructions on how to change the input voltage. Turn the switch to the ON position. Since there are vacuum tubes contained in this instrument, a few minutes warm-up will be required.

2. Insert the resistor to be tested in the test jig, making sure that firm contact is made with the resistor lead. Before closing the top, make sure that the voltage to be applied to the resistor is not excessive.

3. Set RESISTOR RANGE control to the value indicated for the test resistor.

4. Set the FUNCTION switch to CALIBRATE. Close the test jig top and adjust the CALIBRATE ADJUST control until the NOISE meter reads at the CAL line (10 db). Switch the FUNCTION switch to SYSTEM NOISE and note noise reading on NOISE meter. If necessary, adjust METER MULTIPLIER to give an on scale reading.

5. Switch FUNCTION switch to TOTAL NOISE and adjust VOLTAGE ADJUST to appropriate voltage. Typical voltage values can be obtained from Table 1-1.

6. To obtain the Noise Index, microvolts per volt in a decade, merely subtract the dc voltage reading (D) in db from the total noise voltage reading (T) in db. For resistors having small amounts of noise, that is, a small difference between system noise (S) and total noise, a correction factor f(T — S), must be applied. This correction factor may be obtained from the graph in Figure 1-2. Thus the Index = T — [f(T — S)] — D in db.

7. Noise Index in db may be converted to noise voltage in microvolts/volt by referring to Figure 1-1.

DIODE MEASUREMENTS

ZENER DIODES:

1. Turn the instrument on and allow to warm up for a few minutes.

2. Place a short circuit in the test jig, set the FUNCTION switch to CALIBRATE and adjust the NOISE meter to the CAL line (10 db).

3. Set the FUNCTION switch to SYSTEM NOISE and note the NOISE meter reading. (This reading should be somewhat less than —8 db.) Remove the short circuit.

4. Select the appropriate position on the RESISTOR RANGE switch.

Resistor Range	$R_{IS} = R_M +$ R301 + R303	Zener Current
0.1K— < 2.5K	2,600	10- 30 ma
2.5K— < 25K	11,600	3- 10 ma
25K— <250K	100K	0.3- 3 ma
250K— 22M	1 Meg	30-300 μa

5. Calculate the required DC supply voltage, which equals the Zener voltage plus the Zener current times the isolating resistor. $V_{DC} = V_Z + (I_Z \times R_{IS})$ (For example, a 6 volt Zener with 5 ma through it. $6 + [(5 \times 10^{-3})\ (11.6 \times 10^3)] = 64$ VDC). *WARNING:* Do not exceed the maximum Zener current for each range to limit dissipation in the isolating resistor.

6. Close the cover and set the FUNCTION switch to TOTAL NOISE. Set the VOLTAGE ADJUST control to the value calculated in Step 5.

7. Insert the Zener Diode in the jig and close the cover. The DC Voltmeter will read the Zener voltage, and the Noise meter the Zener noise. If there is less than 10 db difference from the value noted in Step 3, use the Correction Chart for Presence of System Noise, Figure 1-2, as with resistors.

BACK-BIASED DIODES:

1. Turn the instrument on and allow to warm up for a few minutes.

2. Place a short circuit in the test jig, set the FUNCTION switch to CALIBRATE, and adjust the NOISE meter to the CAL line (10 db). Remove the short circuit.

3. Set the RESISTOR RANGE switch to the 250K-22M position. Set the FUNCTION switch to SYSTEM NOISE, close the test jig cover, and note the NOISE reading (this reading should be somewhat less than 18 db).

4. Set the FUNCTION switch to TOTAL NOISE and set the VOLTAGE ADJUST control to the desired voltage. *NOTE:* The minimum supply voltage in the Model 315 is 20-30 volts.

5. Insert the diode in the test jig and close the cover.

Note the noise reading. If there is less than 10 db difference from the value noted in Step 3, use the Correction Chart for Presence of System Noise, Figure 1-2, as with resistors.

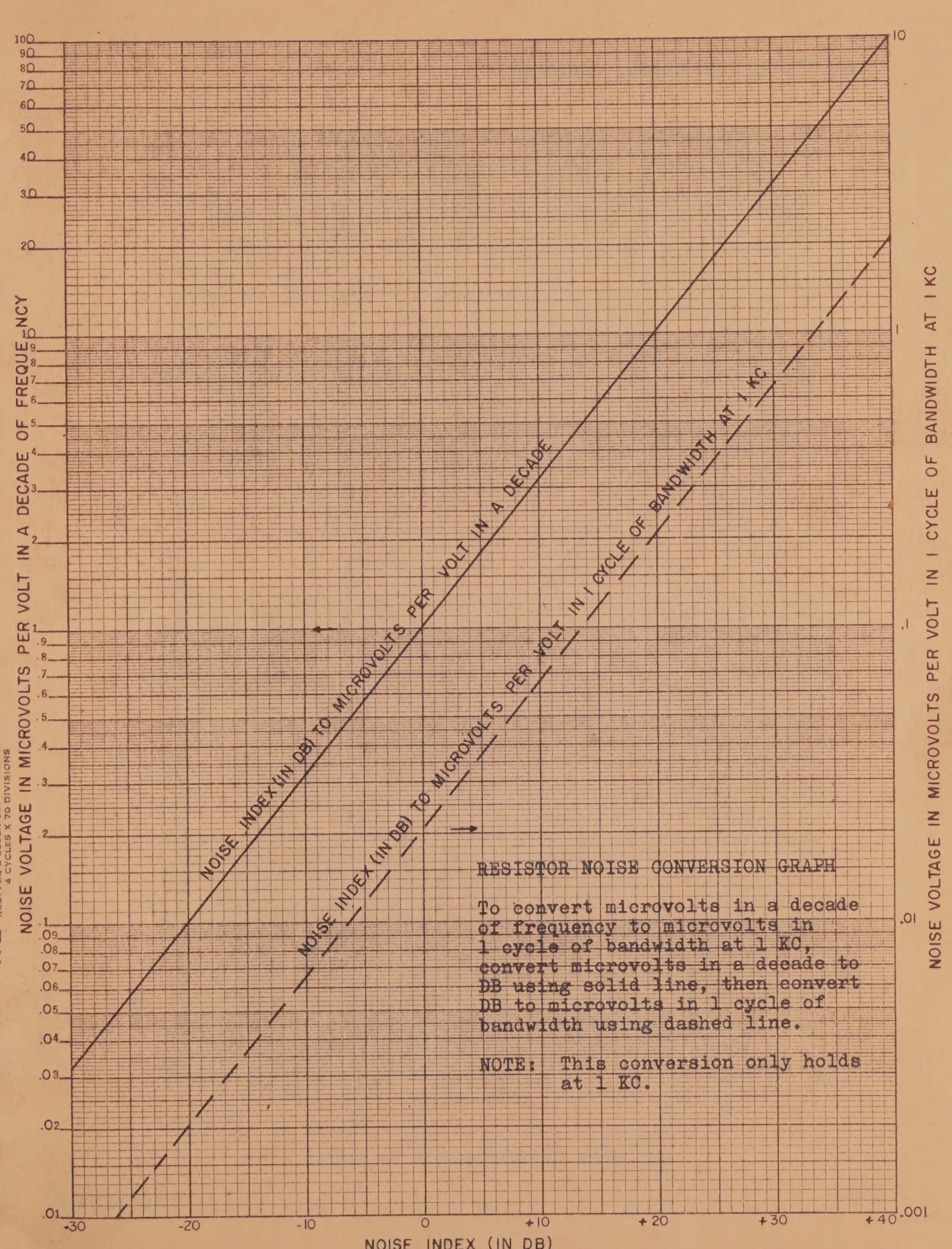
6. If the DC Voltage reading changes from Step 4, it indicates leakage in the diode, which may be calculated ăs the difference between the two voltage readings through the 1 megohm isolating resistor.

REMOTE OPERATING CABLE, TYPE 1107

This instrument is supplied with a Remote Cable, Type 1107. Extreme care should be exercised when using this cable to prevent errors in noise readings due to extraneous noise or hum pickup or capacitive loading of the signal lead. The cable termination should be properly shielded from both magnetic and electrostatic fields and the signal lead should be provided with a low capacitance interlock switch to prevent the operator coming in contact with the high voltage present when in TOTAL noise position.

When the instrument is used without this remote cable the instrument jack, J302, should be shielded with the shield cover provided.

See Schematics, T-1903 and T-1904, for Remote Cable connections.


NOISE VOLTAGE IN MICROVOLTS PER VOLT IN A DECADE OF FREQUENCY
NOISE VOLTAGE IN MICROVOLTS PER VOLT IN 1 CYCLE OF BANDWIDTH AT 1 KC
NOISE INDEX (IN DB)
NOISE INDEX (IN DB) TO MICROVOLTS PER VOLT IN A DECADE
NOISE INDEX (IN DB) TO MICROVOLTS PER VOLT IN 1 CYCLE OF BANDWIDTH AT 1 KC
RESISTOR NOISE CONVERSION GRAPH
To convert microvolts in a decade of frequency to microvolts in 1 cycle of bandwidth at 1 KC, convert microvolts in a decade to DB using solid line, then convert DB to microvolts in 1 cycle of bandwidth using dashed line.
NOTE: This conversion only holds at 1 KC.
-30
-20
-10
0
+10
+20
+30
+40
100
90
80
70
60
50
40
30
20
10
9
8
7
6
5
4
3
2
1
.9
.8
.7
.6
.5
.4
.3
.2
.1
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.03
.02
.01
10
1
.1
.01
.001

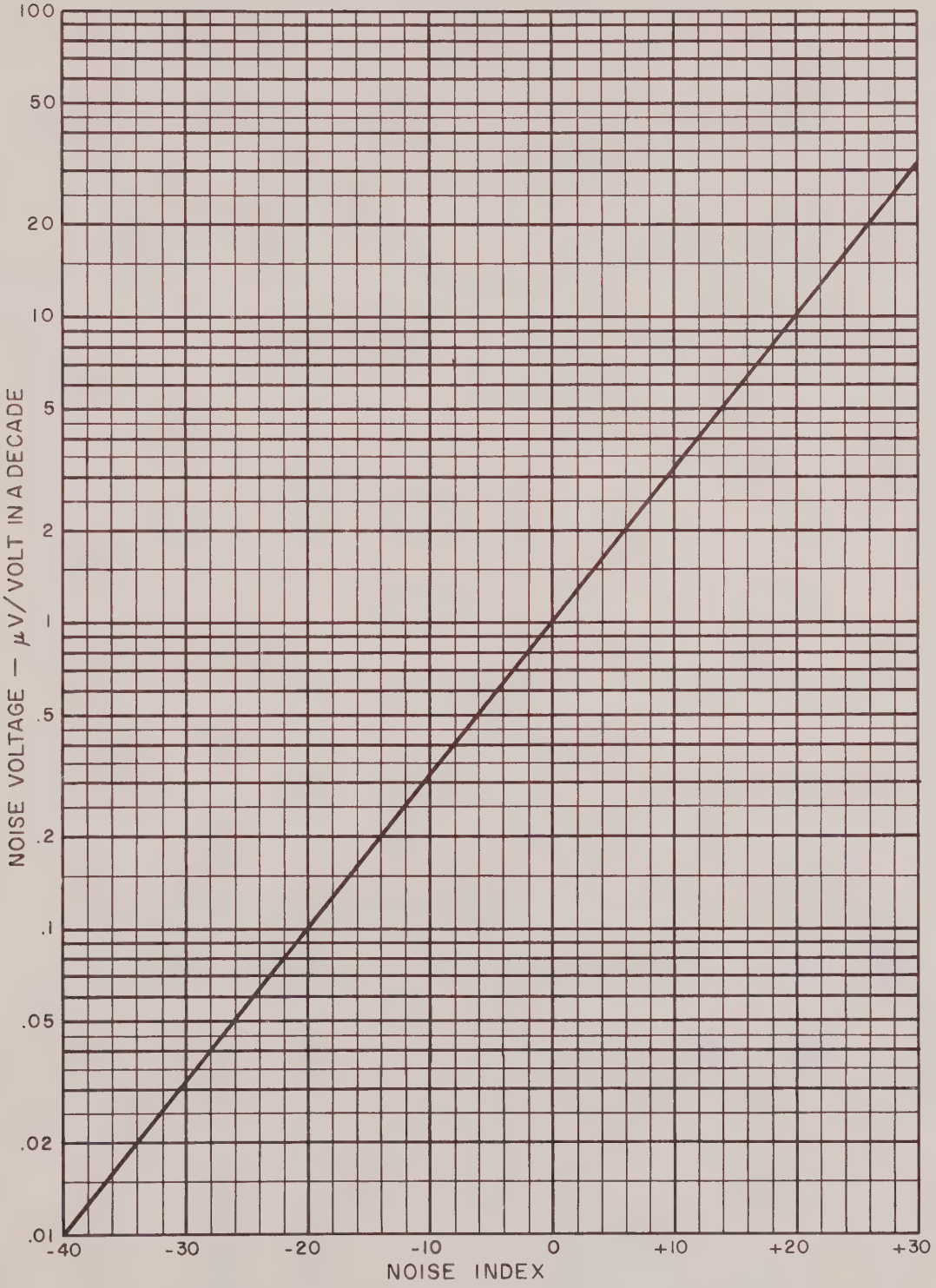


FIGURE 1-1. NOISE CONVERSION GRAPH

TABLE 1-1. RECOMMENDED OPERATING CONDITIONS

R Ω	R_m Ω	½ watt and High Wattage Ratings (D)* db	V Volts	P_{dc} MW	⅛, ¼ and 1/10 Watt Ratings (D)* db	V Volts	P_{dc} MW
100	1 K	10.1	3.2	100	10.1	3.2	100
120	1 K	11.6	3.8	120	10.9	3.5	100
150	1 K	13.5	4.7	150	11.8	3.9	100
180	1 K	15.1	5.7	180	12.5	4.2	100
220	1 K	16.9	7.0	220	13.4	4.7	100
270	1 K	18.3	8.2	250	14.3	5.2	100
330	1 K	19.2	9.1	250	15.1	5.7	100
390	1 K	19.9	9.9	250	15.8	6.2	100
470	1 K	20.7	10.8	250	16.7	6.9	100
560	1 K	21.4	11.8	250	17.5	7.5	100
680	1 K	22.3	13.0	250	18.3	8.2	100
820	1 K	23.1	14.3	250	19.2	9.1	100
1.0 K	1 K	24.0	15.8	250	20.0	10.0	100
1.2 K	1 K	24.8	17.3	250	20.8	11.0	100
1.5 K	1 K	25.8	19.4	250	21.7	12.2	100
1.8 K	1 K	26.6	21.2	250	22.5	13.4	100
2.2 K	1 K	27.4	23.4	250	23.4	14.8	100
2.7 K	10 K	28.3	26.0	250	24.3	16.4	100
3.3 K	10 K	29.2	28.7	250	25.2	18.2	100
3.9 K	10 K	29.9	31.2	250	25.9	19.7	100
4.7 K	10 K	30.8	34.3	250	26.7	21.7	100
5.6 K	10 K	31.5	37.4	250	27.5	23.7	100
6.8 K	10 K	32.3	41.2	250	28.3	26.1	100
8.2 K	10 K	33.2	45.3	250	29.1	28.6	100
10 K	10 K	34.0	50.0	250	30.1	32.0	100
12 K	10 K	34.8	54.8	250	30.9	35.0	100
15 K	10 K	35.8	61.2	250	31.8	39.0	100
18 K	10 K	36.6	67.1	250	32.5	42.0	100
22 K	10 K	37.4	74.2	250	33.4	47.0	100
27 K	100 K	38.3	82.2	250	34.3	52.0	100
33 K	100 K	39.2	90.8	250	35.1	57.0	100
39 K	100 K	40.0	98.7	250	35.8	62.0	100
47 K	100 K	40.7	108	250	36.7	69.0	100
56 K	100 K	41.5	118	250	37.5	75.0	100
68 K	100 K	42.3	130	250	38.3	82.0	100
82 K	100 K	43.1	143	250	39.2	91.0	100
100 K	100 K	44.0	158	250	40.0	100	100
120 K	100 K	44.8	173	250	40.8	110	100
150 K	100 K	45.8	194	250	41.7	122	100
180 K	100 K	46.5	212	250	42.5	134	100
220 K	100 K	47.5	234	250	43.4	148	100
270 K	1 M	38.6	85.0	26.8	38.6	85.0	26.8
330 K	1 M	40.0	99.0	29.7	40.0	99.0	29.7
390 K	1 M	41.0	112	32.2	41.0	112	32.2
470 K	1 M	42.1	127	34.3	42.1	127	34.3
560 K	1 M	43.1	143	36.5	43.1	143	36.5
680 K	1 M	44.2	161	38.1	44.2	161	38.1
820 K	1 M	45.1	180	39.5	45.1	180	39.5
1.0 M	1 M	46.0	200	40.0	46.0	200	40.0
1.2 M	1 M	46.8	218	39.6	46.8	218	39.6
1.5 M	1 M	47.6	240	38.4	47.6	240	38.4
1.8 M	1 M	48.0	250	34.7	48.0	250	34.7
2.2 M	1 M	48.0	250	28.4	48.0	250	28.4
2.7 M	1 M	48.0	250	23.2	48.0	250	23.2
3.3 M	1 M	48.0	250	18.9	48.0	250	18.9
3.9 M	1 M	48.0	250	16.0	48.0	250	16.0
4.7 M	1 M	48.0	250	13.3	48.0	250	13.3
5.6 M	1 M	48.0	250	11.2	48.0	250	11.2
6.8 M	1 M	48.0	250	9.2	48.0	250	9.2
8.2 M	1 M	48.0	250	7.6	48.0	250	7.6
10 M	1 M	48.0	250	6.2	48.0	250	6.2
12 M	1 M	48.0	250	5.2	48.0	250	5.2
15 M	1 M	48.0	250	4.2	48.0	250	4.2
18 M	1 M	48.0	250	3.5	48.0	250	3.5
22 M	1 M	48.0	250	2.8	48.0	250	2.8

* $D = 20 \log_{10} V$

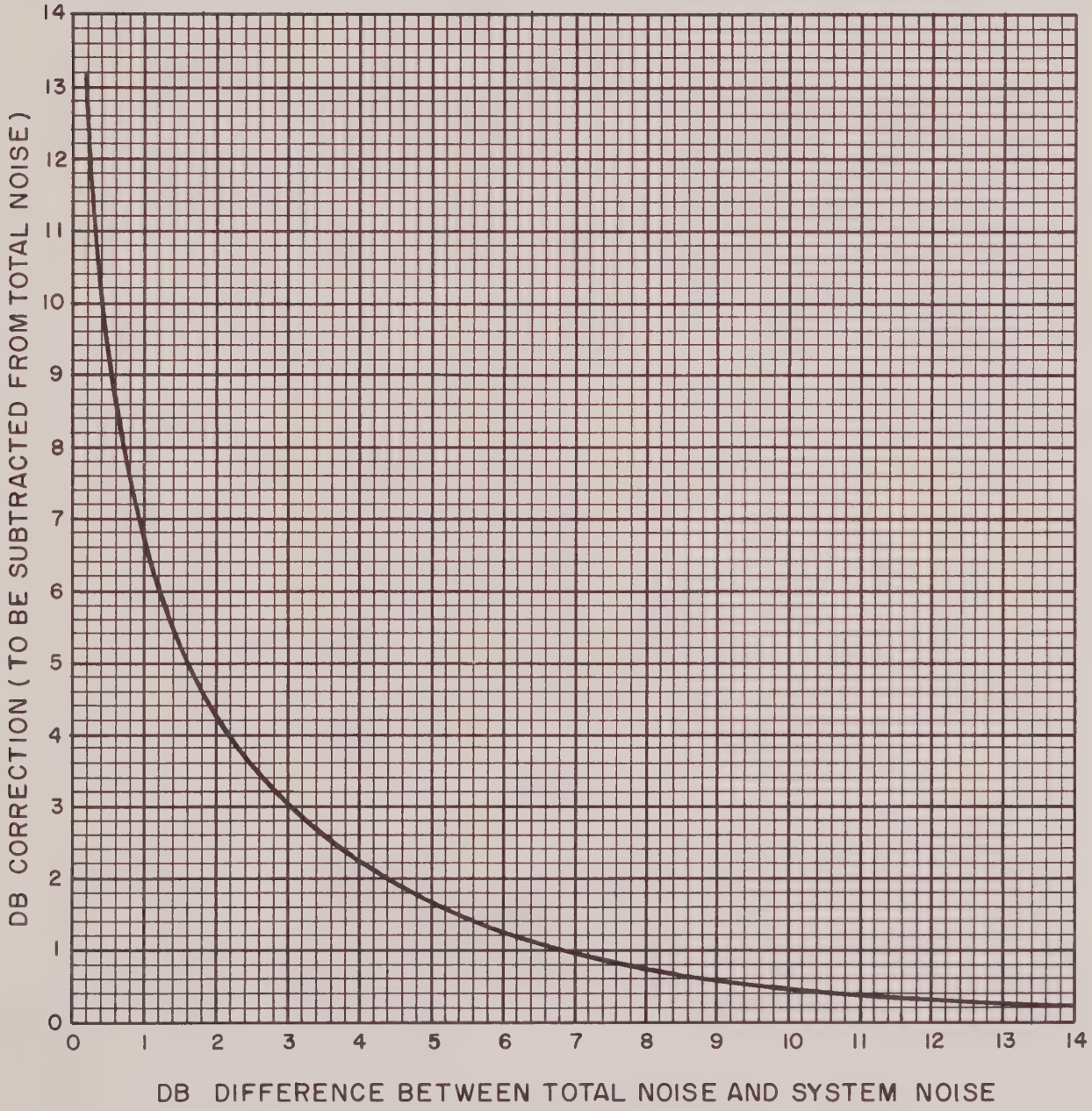


FIGURE 1-2. CORRECTION CHART FOR PRESENCE OF SYSTEM NOISE

SECTION 2

THEORY OF OPERATION

The Model 315 is completely self-contained and requires no accessories for operation. Basically, this instrument serves to measure the increase in noise due to current passing through a resistor.

The simplified block diagram of the system shown in Figure 2-1 illustrates the principles of operation. The dc supply supplies a variable dc voltage from 30 to 450 volts to the test resistor and is isolated by the isolation resistors shown. The dc voltage across the resistor is measured with a vacuum tube voltmeter and the ac noise is amplified, filtered and metered with a thermal type meter. Since the test resistors are of different impedances, calibration of each different value may be made by adjustment of the system gain. Thus, the noise measured is equivalent to that which would come from a 1 ohm generator in series with a test resistor in the same manner as the calibration source.

Figure 2-2 of the detailed block diagram is an elaboration of the simplified diagram and is given in order to simplify servicing and location of parts in the equipment should it be required.

Figure 2-3, Typical Filter, is a plot of the four section Butterworth Bandpass Filter employed in the instrument. Slight deviations (in the order of a few percent) may be found from unit to unit. The filter has been designed with a center frequency of 1000 cycles and having a 1000 cycle bandpass.

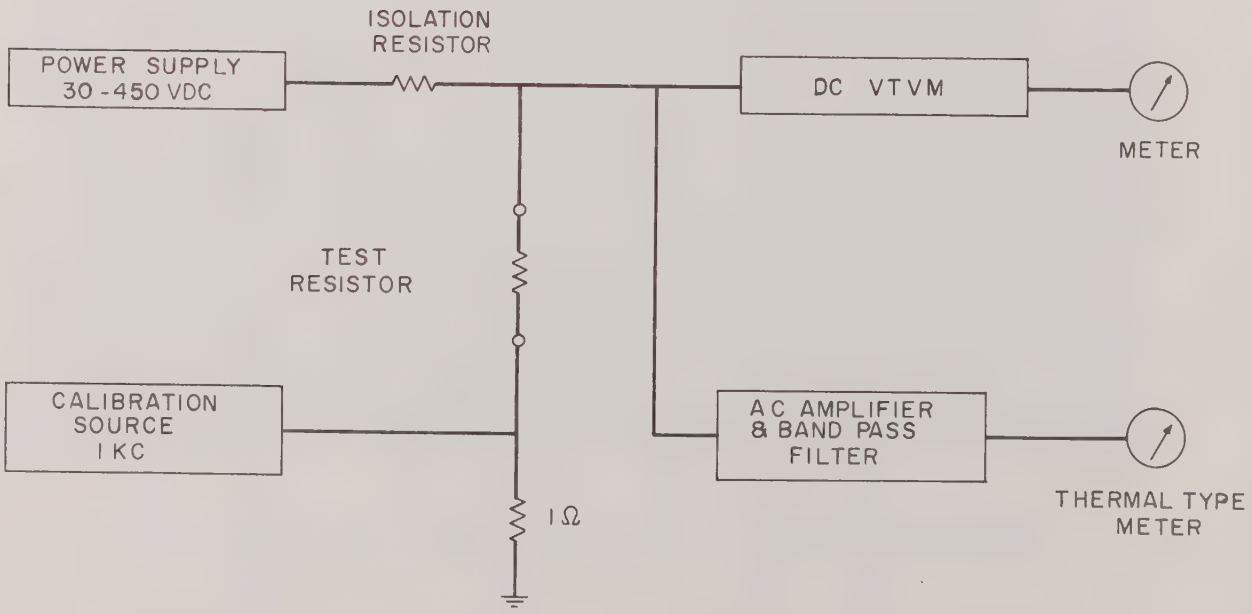


FIGURE 2-1. BLOCK DIAGRAM OF SYSTEM

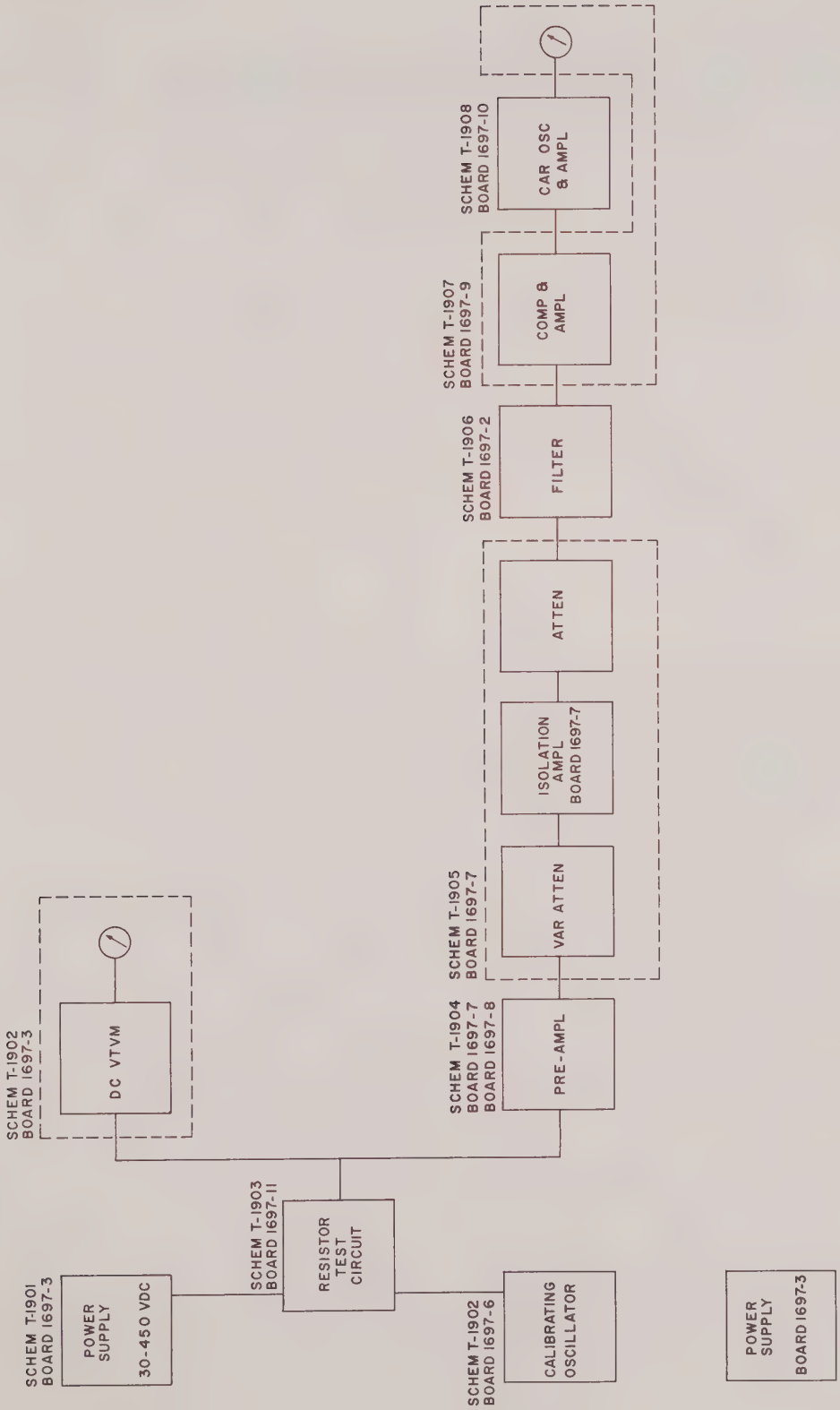


FIGURE 2-2. DETAILED BLOCK DIAGRAM — MODEL 315

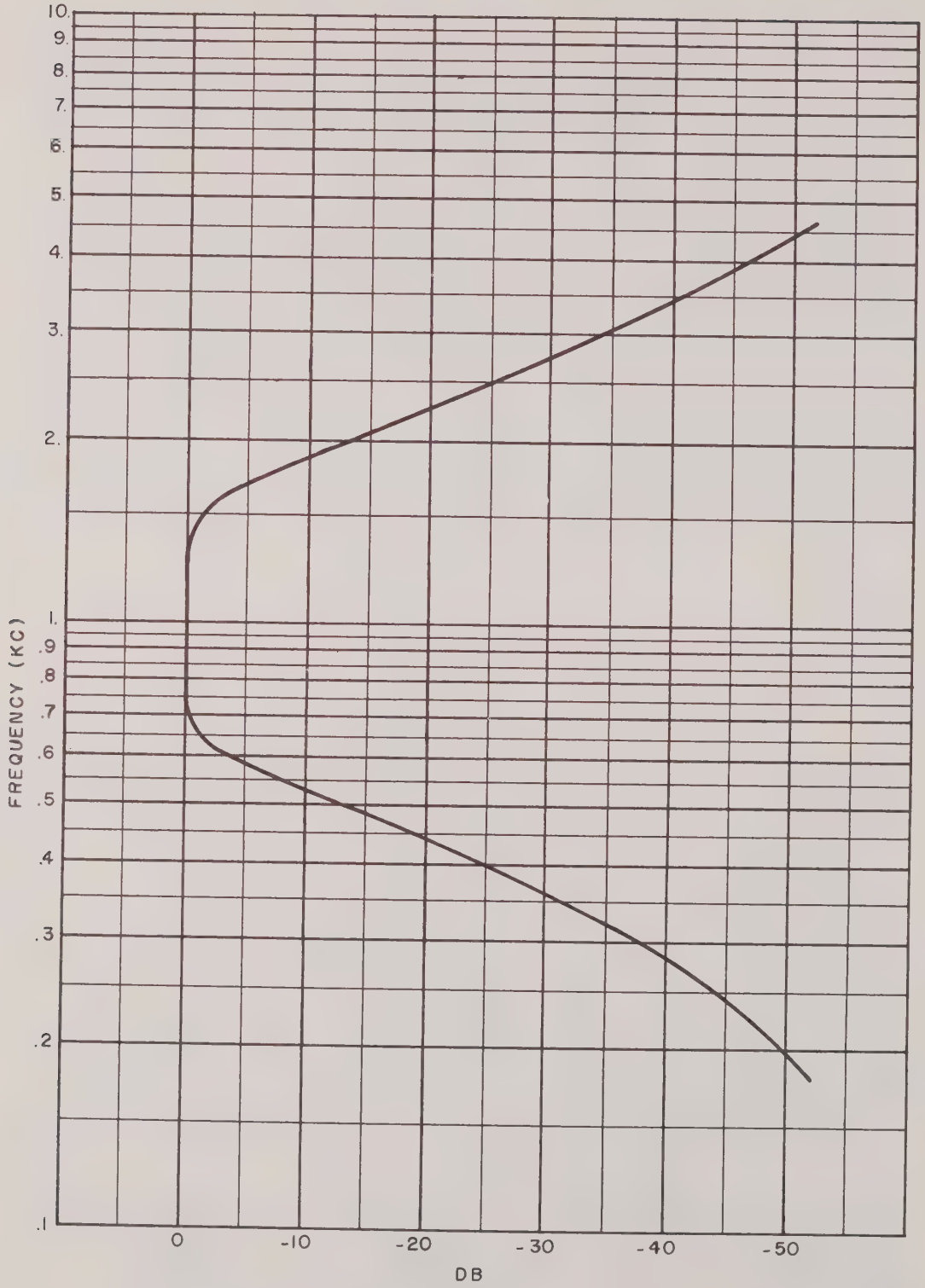


FIGURE 2-3. TYPICAL FILTER

SECTION 3

GENERAL CURRENT NOISE DISCUSSION

The limitation in sensitivity of electronic systems due to noise has been known for over 30 years. Even ideal amplifiers have a threshold determined by the resistance of the signal source. Nyquist's formula, based on the statistical theory of thermodynamics, gives the noise voltage at the terminals of an impedance.

$$\overline{E_{th}^2}^{1/2} = (4k\ T\ B\ R)^{1/2} \qquad \text{eq. 1}$$

where $\overline{E_{th}^2}^{1/2}$ = rms value of the thermal noise voltage, in volts.
k = Boltzman's constant, 1.38×10^{-23} Joules/degree.
T = Temperature in degrees Kelvin.
B = Bandwidth of measuring system in cycles.
R = Real part of the impedance Z, in ohms.

Although most engineers are experienced with the noise generated in vacuum tubes, few have an understanding of the types or magnitudes of noise generated in other electronic devices such as, transistors and other semi-conductors, electrolytic capacitors, and current carrying resistors. Perhaps one of the least realized, but important source of noise, is that of current carrying resistors.

If current is passed through a resistor, an increase in noise above the thermal noise occurs. In wire wound, and some metal film resistors, this effect is of second order and may not be detectable unless the resistors are faulty. However, in resistors, such as composition, deposited carbon resistors, and certain metal film resistors, the effect is by no means negligible and may exceed the theoretical value by an order of magnitude or more. The use of such noisy resistors in critical points of low level circuits may increase the noise at the input by the same factor.

Unlike thermal noise, which is "flat" or independent of frequency (well into the gigacycle region), resistor current noise has a decreasing power vs. frequency spectrum. The relationship of frequency, dc current, and noise in a resistor is given in the equation,

$$\overline{e\,(f)^2} = C\,I^{\alpha} f^{-\gamma} \qquad \text{eq. 2}$$

where $\overline{e\,(f)^2}$ = Mean square noise voltage per cycle of bandwidth at a frequency f.
C = Constant dependent upon the noise quality of the resistor.
I = dc current in amps.
f = Frequency in cycles.
α = 1.4 to 2.2 dependent upon the resistor, and has a mean value of 1.9.
$\gamma \cong 1.0$.

Thus, for most purposes equation 2 may be written,

$$\overline{e\,(f)^2} = C\,I^2 f^{-1} \qquad \text{eq. 3}$$

showing the $1/f$ characteristics of noise power spectral density.

The resistor current noise for a given bandwidth may be obtained by integration of $\overline{e\,(f)^2}$

$$\overline{E_c^2} = \int \overline{e\,(f)^2}\,df \qquad \text{eq. 4a}$$

Since $\overline{e\,(f)^2} = CI^2 f^{-1}$, then

$$\overline{E_c^2} = \int CI^2 f^{-1}\,df \qquad \text{eq. 4b}$$

$$\overline{E_c^2} = CI^2 \ln f \Big|_{f_1}^{f_2} \qquad \text{eq. 4c}$$

$$\overline{E_c^2}^{1/2} = \left[CI^2 (\ln f_2 - \ln f_1) \right]^{1/2} \qquad \text{eq. 4d}$$

or

$$\overline{E_c^2}^{1/2} = \left[CI^2 \ln \left(\frac{f_2}{f_1} \right) \right]^{1/2} \qquad \text{eq. 4e}$$

It can be seen from Equation 4e that bandwidths having equal ratios of upper to lower cut-off frequencies, such as octaves or decades of bandwidth, the current noise magnitudes are equal.

SECTION 3 - GENERAL CURRENT NOISE DISCUSSION

The National Bureau of Standards has recommended the unit microvolts per volt in a decade in db as a standard for current noise in a resistor. There are two advantages of this unit; one, the ease of measurement; and two, the familiarity of the terms for the engineer.

The above unit or INDEX is defined as:

$$\text{INDEX} = 20 \log \frac{\overline{E_c^2}^{1/2}}{V} \text{ db (in a decade of frequency)} \qquad \text{eq. 5}$$

Therefore equation 4e may be changed to

$$\overline{E_c^2}^{1/2} = V\, 10^{\text{INDEX}/20} \left(\log \frac{f_2}{f_1} \right)^{1/2} \qquad \text{eq. 6}$$

where $\overline{E_c^2}^{1/2}$ = total rms current voltage.
V = dc voltage.
f_1 & f_2 = lower and upper effective bandpass limits.

Since current noise is of a $1/f$ nature, its effect will be masked by thermal noise at higher frequencies. In practice, this is usually true above 100 kc. Both thermal noise and current noise have a Gaussian or normal voltage amplitude distribution. Since their sources are independent they may be added as shown,

$$\overline{E_{\text{Total}}^2}^{1/2} = \left[\overline{E_c^2} + \overline{E_{th}^2} \right]^{1/2} \qquad \text{eq. 7}$$

Figure 3-1 shows the noise spectral density as a function of frequency of a typical 10 K ½ watt resistor with 20 volts dc applied.

This resistor has a current noise INDEX of approximately —10 db (0.3 μv/v in a decade). It has been found from the evaluation of a large quantity of composition resistors that nearly all fall in the range of 0.1 to 10 μv/v in a decade of current noise.

We may add the noise in decades in an r m s fashion. That is, for 2 decades of $1/f$ noise we have $\sqrt{2}$ times as much noise voltage, and for 3 decades $\sqrt{3}$ times as much. It should be pointed out that we have not added equal bandwidths but equal percentage bandwidths. Thus, for bandwidths other than one decade equation 6 must be used.

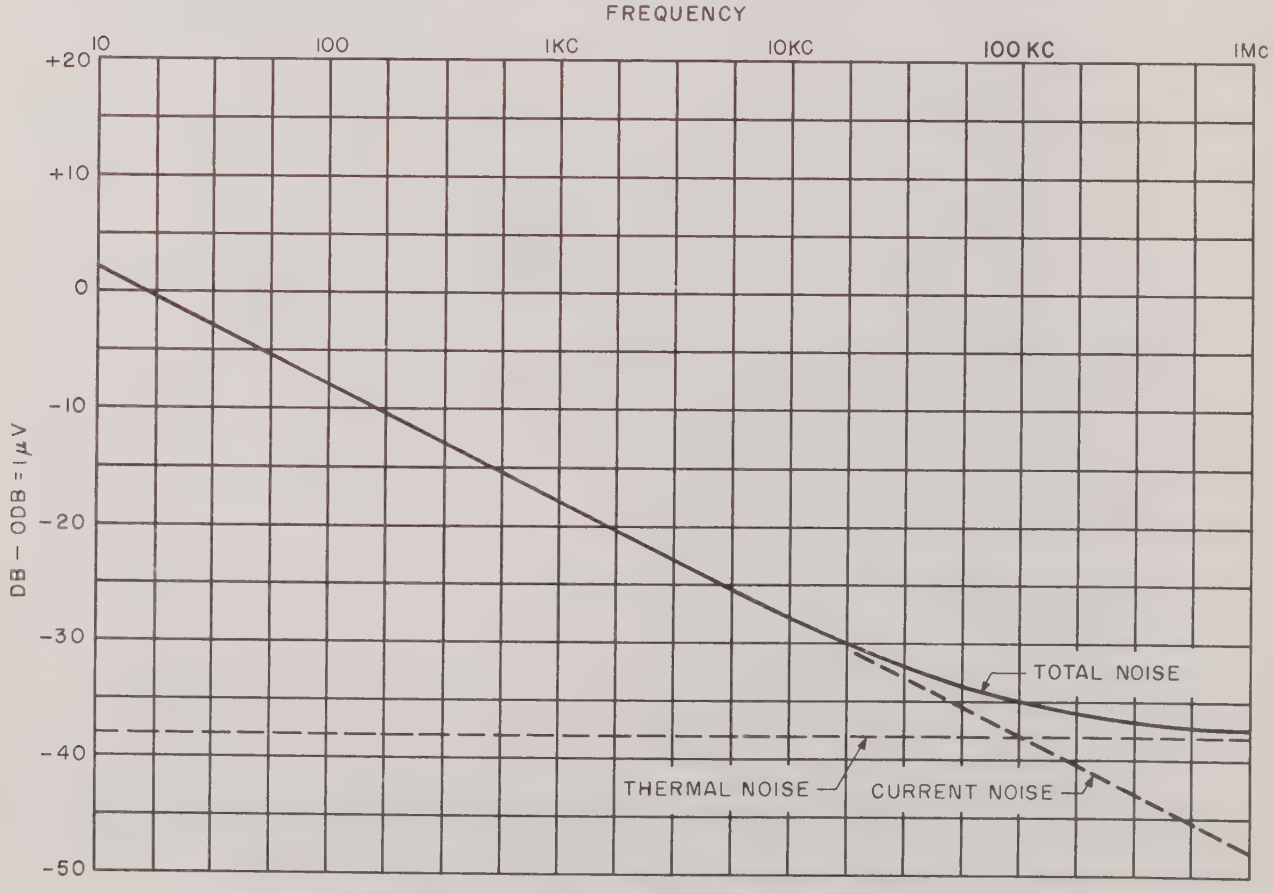


FIGURE 3-1. NOISE VOLTAGE SPECTRAL DENSITY 10K OHM COMPOSITION RESISTOR, 20 VDC

SECTION 3 - GENERAL CURRENT NOISE DISCUSSION

APPLICATIONS:

In order to apply the Index of current noise of a resistor in circuit design one must know the Index, the voltage and the position in the circuit. Let us look at a few practical applications of this noise. Since composition resistors of reasonable quality have an Index reasonably close to 0 db in a decade, we can see that the current noise voltage is more a function of the applied dc voltage than of the value of the resistor.

Assume a 10 K resistor has an Index of 0 db. This resistor will appear as a noise generator of 10 K impedance and for every volt of dc applied to its terminals the generator will develop 1 μv of current noise in one decade of bandwidth, or, in a bandwidth from 10 cycles to 10 kc (three decades) 1.73 μv/v of noise. For ten volts dc it would generate 17.3 μv of noise. By comparison, the thermal noise over the same bandwidth would be 1.25 μv. If this resistor were the bias resistor of a transistor input stage as shown in Fig. 3-2(a) the noise would be 14 times the theoretical minimum.

The effects of current noise are quite noticeable even in the plate circuits of vacuum tube amplifiers, and to a lesser extent in transistor collector circuits. The 100K resistor in Fig. 3-2(b) having a noise Index of 0 db and 100 volts applied voltage would result in approximately 5.5 μv of noise equated to the input, or an equivalent input resistance of 0.16 megohms. In this application negative feedback would reduce the noise in proportion to the feedback.

Similar results will be found in operational amplifier feedback, resistors, power supply references, servo loops, etc.

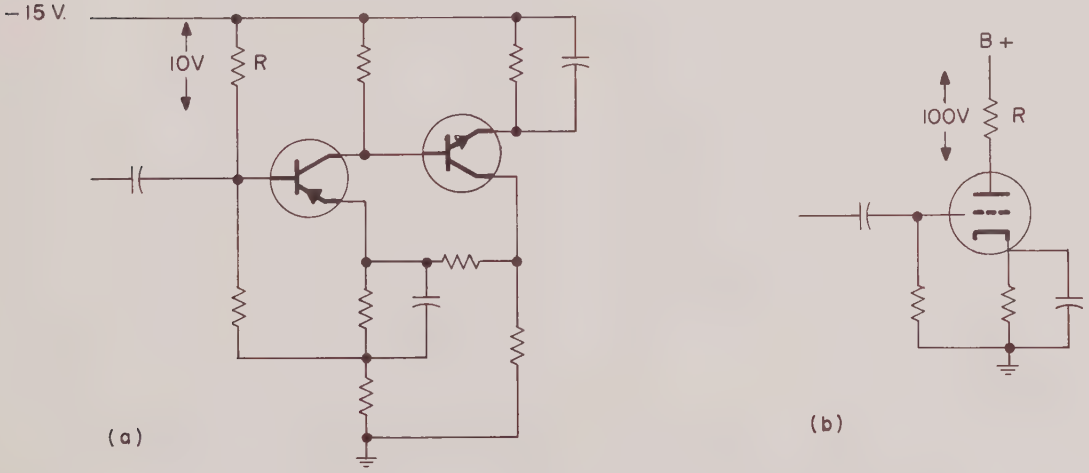


FIGURE 3-2. TYPICAL RESISTOR CURRENT NOISE SOURCES

SECTION 4
CIRCUIT ANALYSIS

POWER SUPPLY
(Board No. 1697-3) (Schematic T-1901)

The power supply shown on Schematic T-1901 supplies all regulated dc for the instrument. The reference for these supplies is the Zener Diode CR112. Transistors Q104, Q105, Q106 and Q107 form a double differential amplifier. Q106 drives the base of Q103 which is the pass transistor and supplies —26 volts for the transistor amplifiers, filters, measuring circuit and the filaments of all vacuum tubes except V101. Q101 and Q102 function as a sub-supply for +26 volts used in the vacuum tube voltmeter. The reference for this sub-supply is formed by the voltage divider network R103 and R117. The variable output voltage (+30 to +450 volts) is obtained from V101 and is varied by R107 which in conjunction with R106 and R127 form a voltage divider and obtains its reference from the CR112. Q109 and Q108 form an emitter coupled amplifier to drive V104, and in turn V101. The +300 volt and +150 volt output obtained from V102 and V103 supply voltage for the vacuum tube voltmeter and preamplifier tubes respectively.

VACUUM TUBE VOLTMETER
(Board No. 1697-3) (Schematic T-1902)

The vacuum tube voltmeter design consists of a balanced pair of tubes V202 and V203. The meter multiplier attenuator merely acts as a shunt at the grid and is in series with the 8 megohm resistor found in the resistor test circuit schematic. V201 is a protective diode to clamp severe overloads and keep them from reaching the transistorized portion of the circuit. Q201 and Q203 act as grounded collector impedance converters. Q202 operates as a differential detector and drives the output meter and dc analog output. The meter is adjusted to read full scale for 10 volts at the analog output.

CALIBRATING OSCILLATOR
(Board No. 1697-6) (Schematic T-1902)

The calibrating oscillator consists of a single transistorized transformer coupled oscillator with a resonant tank in the collector circuit. The magnitude of oscillation is controlled from the base tie point and may be adjusted over narrow limits by R221. The magnitude of the 1000 cycle signal at the output to the test circuit should be 650 microvolts. The calibrating oscillator circuit is separately regulated by CR204.

RESISTOR TEST CIRCUIT
(Schematic T-1903)

The sensitive portion of the resistor test circuit is enclosed in an iron shield below the chassis, and the position of leads in this area is critical.

PRE-AMPLIFIER
(Board No. 1697-7) (Schematic T-1904)

The entire pre-amplifier is doubly shielded, and well filtered supplies are required. The amplifier consists of V401 and V402 operating as cathode followers in parallel, thus reducing the equivalent noise resistance at the input. Adjustment of R401 will vary the plate voltage on the tubes to an optimum point, normally about 50 volts. Excessive voltage increases the noise, and insufficient voltage may cause grid current to flow and again result in excessive noise for high input impedance. Q401, Q402 and Q403 form a PNP-NPN-PNP amplifier having a large amount of feedback, and a gain of approximately 75.

ISOLATION AMPLIFIER AND ATTENUATOR
(Board No. 1697-7) (Schematic T-1905)

The purpose of the isolation amplifier is to provide isolation and gain between the variable gain adjust (CALIBRATE ADJUST) and the meter multiplier attenuator. It consists of a PNP-NPN-PNP feedback triple and has a gain of approximately 150.

FILTER AMPLIFIER
(Board No. 1697-2) (Schematic T-1906)

The filter consists of a 4 section Butterworth filter, and each filter section operates essentially in the same manner. The output impedance of each transistorized amplifier in the filter is quite low, and the input impedance is determined by the base biasing resistors of each section. The Q of each of the filter resonant sections is determined by the respective base biasing resistors. Thus, each section of the filter is isolated from the other, and gain is obtained without overload due to interference.

MEASURING CIRCUIT

Compressor and Amplifier (Board No. 1697-9) (Schematic T-1907)

Carrier Oscillator and Amplifier (Board No. 1697-10) (Schematic T-1908)

The entire meter amplifier consists of an input voltage amplifier Q701 and Q702, volume compressor CR701, CR702, CR703, CR704 and Q703, a power amplifier Q704, Q705, Q706 and Q707, a hot wire element R729 and a level detector. The principle of operation of this part of the circuitry is to provide the hot wire element R729 with a constant average amplitude signal. This signal results in heating of the resistive element. The resistance due to heating of the element is then detected by measuring the magnitude of a 100 KC carrier signal which is supplied to the hot wire element by Q803. Q802, Q801 amplify the carrier signal across the hot wire element. This signal is rectified by CR801 and CR802. A threshold detector and amplifier consisting of Q709 and Q708 amplify the error signal between the reference threshold (adjustable by R735) and in turn control the volume compressor to maintain a constant amplitude signal again at R729, the hot wire element. This signal should be in the order of 2 volts.

SECTION 5

MAINTENANCE AND CALIBRATION

The components and transistors in the Model 315 are conservatively rated and should provide long and trouble free service. If, however, the instrument has been damaged and recalibration or alignment is required, the following instructions should be followed explicitly, or the instrument returned to the factory. Instructions are given on the Warranty page for the procedure to be followed should it be desired to return the instrument for any reason.

Although the Model 315 is a complex instrument, trouble shooting can readily be done in sections as indicated in the Block Diagram, Fig. 2-2.

Do not change any adjustments without a thorough knowledge of the circuit and the functions of the adjustment.

Standard transistor servicing care should be used throughout. Transistors can be easily damaged with large transient voltages. Therefore, take great care not to short any terminals when making measurements on the printed-circuit boards.

In soldering to the printed-circuit boards, have the iron only hot enough to make a rapid clean solder joint. DO NOT use a solder gun. DO NOT apply any force that would tend to push the copper away from the board.

REMOVAL FROM CASE

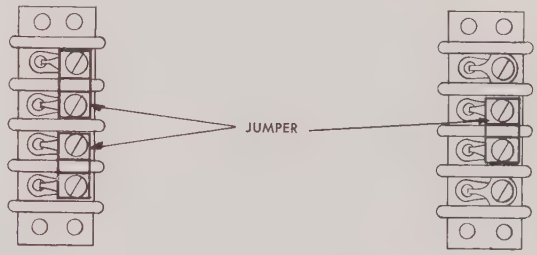
1. Remove the four (4) feet and the two (2) binder head screws from the bottom of the case.
2. Slide the instrument gently out of the front of the case.

CHANGING INPUT VOLTAGE

This instrument has been designed to operate from a 117 V.A.C. or a 234 V.A.C. power source. The plate on the rear of the instrument near the power cord indicates the voltage and frequency at which the instrument should be operated.

Should it be desired to change the input voltage,

1. Remove the instrument from the case.
2. Change the transformer primary connections by moving the jumpers on the 4 terminal barrier strip located near the power cord (See Figure 5-1).
3. Change the fuse. For 117 V.A.C. operation, the fuse should be ¾ Amp. Slow Blow; for 234 V.A.C. operation the fuse should be ⅜ Amp. Slow Blow.
4. Reverse the plate located near the power cord to read the correct voltage.



For 117 V.A.C. operation **For 234 V.A.C. operation**

FIGURE 5-1. INPUT VOLTAGE BARRIER STRIP

CALIBRATION

Before alignment is attempted the operator should become familiar with the Theory of Operation of this instrument, see Theory of Operation, Section 2, then proceed as follows:

POWER SUPPLY

CAUTION: The power supply contains high voltages.

1. −26 Volt Supply

a. Remove the 807 tube (V101).

b. Apply power and adjust R114 to obtain −26 Volts relative to ground on Pin #4, V104 (Board No. 1697-3).

c. Adjust R110 for minimum ripple and best regulation to line voltage variations.

d. Re-adjust R114 to again obtain −26 Volts.

2. +26 Volt Supply

a. Measure the +26 Volt supply at Pin #7, V104. The voltage will normally be between +25 to +27 volts.

b. No adjustment is provided, but the voltage may be changed by modification of R117A if necessary.

3. +150 and +300 Volt Supplies

a. Measure the VR regulated supplies. These voltages should be approximately +300V on Pin #5 of V102 and +150V on Pin #5 of V103.

CAUTION: *DO NOT* operate the power supply with any but the 807 tube (V101) removed.

4. Heater Voltages

a. Measure the heater voltage on Pins #4 and #5 of the 5879 tubes, V104, V201, V202 and V203. Heater

voltage should be between 6VDC and 7VDC. These tubes are connected in series, and a faulty heater on one will effect all others in the string.

5. V101 Supply

a. Measure the screen and plate voltage of the 807 tube socket and cap with the tube *removed* from the socket. Plate voltage should be +600V to +700V with respect to ground. Screen voltage Pin #2 should be approximately +150V with respect to the cathode (Pin #4).

6. Variable +30 to +450 Volt Supply

a. *Remove power* and insert the 807 tube (V101).

b. Set the VOLTAGE ADJUST control (R107) approximately ⅔ clockwise.

c. Apply power and check the control of the variable regulated voltage as measured at the 807 tube cathode (Pin #4) and ground.

d. With the VOLTAGE ADJUST control full clockwise, the voltage should normally be between 470V to 480V. R127 may be selected to adjust this maximum voltage.

D.C. VACUUM TUBE VOLTMETER

CAUTION: *DO NOT* operate the power supply with any of the 5879 tubes removed.

1. V202 - V203 Balance

a. Ground the input to V202, (Pin #1), and connect a DC voltmeter, 3V range, to the DC ANALOG OUTPUT jack (J201).

b. Select a pair of 5879 tubes for V202-V203 to indicate zero voltage with R216 (Front panel screw driver adjust pot) near the center of its range.

c. A DC voltmeter connected between the cathodes of V202 and V203 (Pins #3) should also indicate zero voltage.

2. DC Voltmeter Calibration

a. Insert a resistor (approx. 470 ohms 2 watt) in the resistor test jig, set the VOLTAGE ADJUST control to minimum setting, and set the METER MULTIPLIER Switch to 0 DB position.

b. Connect a DC voltmeter across the resistor and with the door interlock switch energized set the voltage to 10V. The FUNCTION switch must be in the TOTAL NOISE position in order to obtain a voltage at the resistor terminals.

c. Adjust R207 to obtain 10V dc at the DC ANALOG OUTPUT jack (J201).

d. Switch the voltage METER MULTIPLIER Switch to the +20 DB position and re-adjust the front panel screwdriver adjust control (R216) for an indication of 1V at the DC ANALOG OUTPUT jack (J201).

e. Repeat Para. c & d above until 10V and 1V at J201 is obtained for 0 DB and +20 DB METER MULTIPLIER positions.

f. With 10V present at J201 as above, adjust R210 for 10V indication on DB-VOLTS meter (M201).

g. As some interaction is present in the above adjustments of R210, R207 and R216, the above calibrating sequence must be repeated until 10V at J201 and 10V meter indications are obtained for the 0 DB position of the METER MULTIPLIER Switch (S201) and 1V at J201 and 1V meter indication for the +20 DB position of the METER MULTIPLIER Switch (S201).

h. Remove the 470 ohm resistor from the test jig and check the meter calibration at 100V for the +20 DB position of the METER MULTIPLIER switch and 400V for the +40 DB position of the METER MULTIPLIER switch increasing the VOLTAGE ADJUST control as necessary to obtain the above voltages.

i. Insert a 1.2 megohm resistor in the test jig and with the VOLTAGE ADJUST control at the maximum voltage setting and the RESISTOR RANGE switch (S304) in the 250K - 22M position, the voltmeter should indicate at least 218V (46.8 DB).

CALIBRATING OSCILLATOR

1. Calibration

a. Using a shielded cable and sensitive vacuum tube voltmeter, measure the level of the 1000 cycle calibrating oscillator at the CAL. jack (J301).

b. Adjust this level to 650 microvolts by means of R221 (access to this adjustment may be made through the hole in the side of the chassis).

1 KC FILTER

1. Bandwidth

a. Connect an audio oscillator, approximately 1V at 1000 cycles to the CAL. jack (J301), with the METER MULTIPLIER in the +40 DB position, and the FUNCTION switch in the SYSTEM NOISE position.

b. With a short circuit in the test resistor jig, set the CALIBRATE ADJUST control to obtain a 500 microvolt signal at the input to Q601 as measured with a VTVM. Connect the VTVM to the output of the filter at C614 and measure the flatness of the filter and —3 DB bandwidth.

c. The —3 DB points should normally occur at 618 cycles and 1618 cycles. The band top will normally be flat ±2% over approximately 500 cycles.

d. The bandwidth and bandpass shape are determined by the "Q" adjustments R611, R623, R635 and terminating resistor R645.

METER AMPLIFIER

1. Calibration

a. With a short circuit in the resistor test jig, the FUNCTION switch in the CALIBRATE position, the CALIBRATE ADJUST control full counterclockwise to the minimum gain position, adjust R706 to obtain approximately 260 millivolts RMS at the NOISE jack (J701).

b. Increase the CALIBRATE ADJUST control to obtain 1.00V RMS at the NOISE jack (J701).

c. With the calibrating signal level as in paragraph b, adjust R735 to obtain 10V DC at the NOISE ANALOG jack (J702).

d. With the calibrating signal level as in paragraph b, adjust R716 until the NOISE meter indicates 20 DB.

INTERNAL NOISE

1. System Noise

a. With a short circuit in the resistor test jig, the FUNCTION switch in the CALIBRATE position, set the CALIBRATE ADJUST control for a NOISE meter indication of 10 DB (CAL mark).

b. Switch to SYSTEM NOISE. Residual noise will normally be below —8 DB. (A meter indication of 12 DB with the METER MULTIPLIER switch in the —20 DB position.)

c. Remove the short circuit from the resistor test jig. With the RESISTOR RANGE switch in the 0.1-2.5 K position, the system noise will normally increase 1 to 2 DB.

d. Switch to the 2.5-25K position. The system noise will normally be between —3 and —1 DB.

e. Switch to the 25K-250K position. The system noise will normally be between 5.5 DB and 7.5 DB.

f. Switch to the 250K-22M position. The system noise will normally be between 15 DB and 18 DB.

NOTE: It may be necessary to compromise the adjustment of the cathode follower plate voltage control, R401, (located on rear chassis plate) for optimum noise setting for both short circuit input and 1 megohm (250K-22M position) input.

2. Current Noise

a. Measure resistor current noise for the following values of *good* wire wound resistors (See operating instructions).

1K at 16V DC
10K at 50V DC
100K at 160V DC
1 Meg. at Maximum voltage

b. No increase over system noise will normally be observed.

SCHEMATIC LEGEND

K = 1000

⊘ = Screw Driver Adjustment

▭ = Front Panel Control

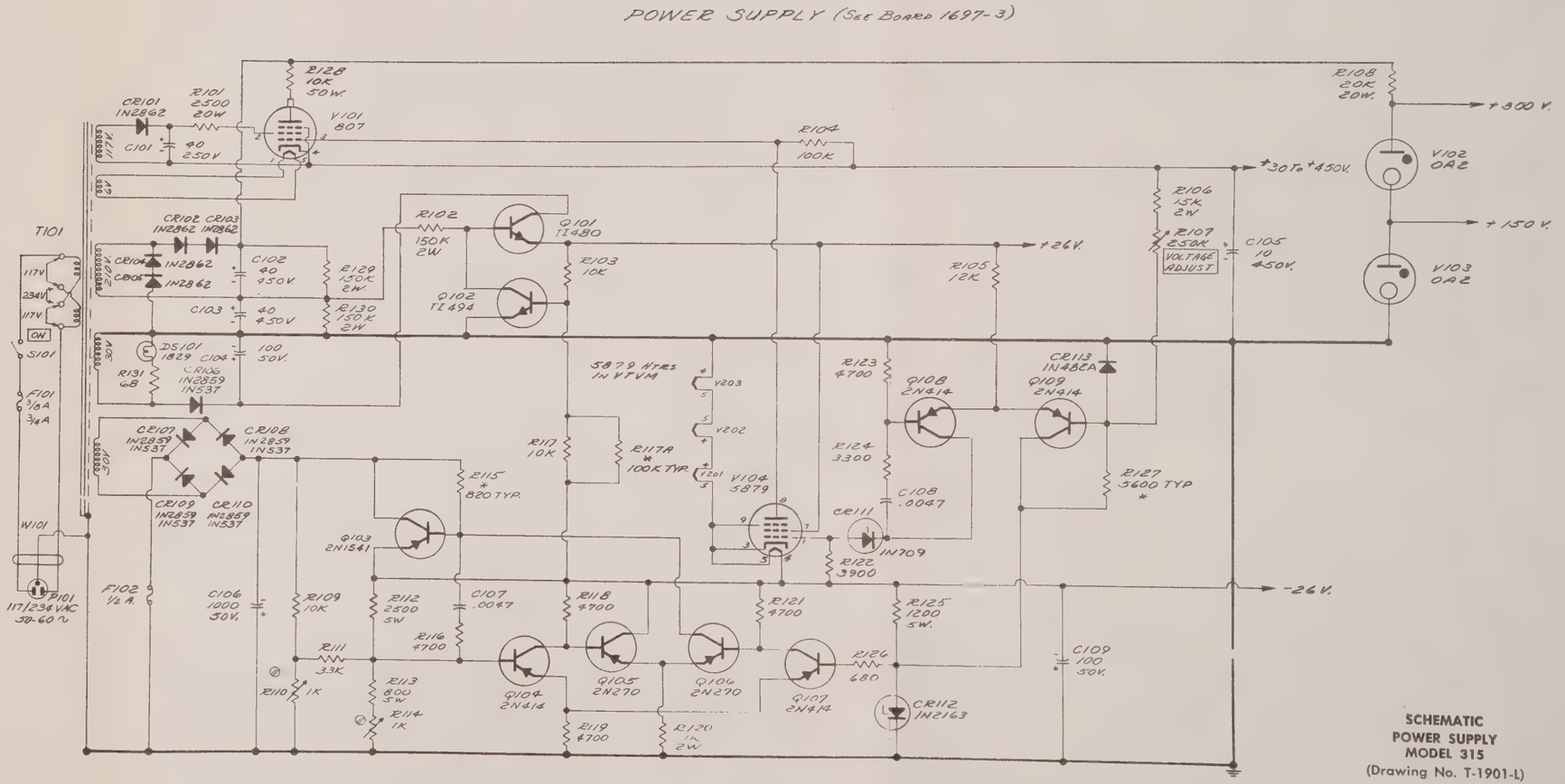
* = Factory Select

Unless Otherwise Specified:

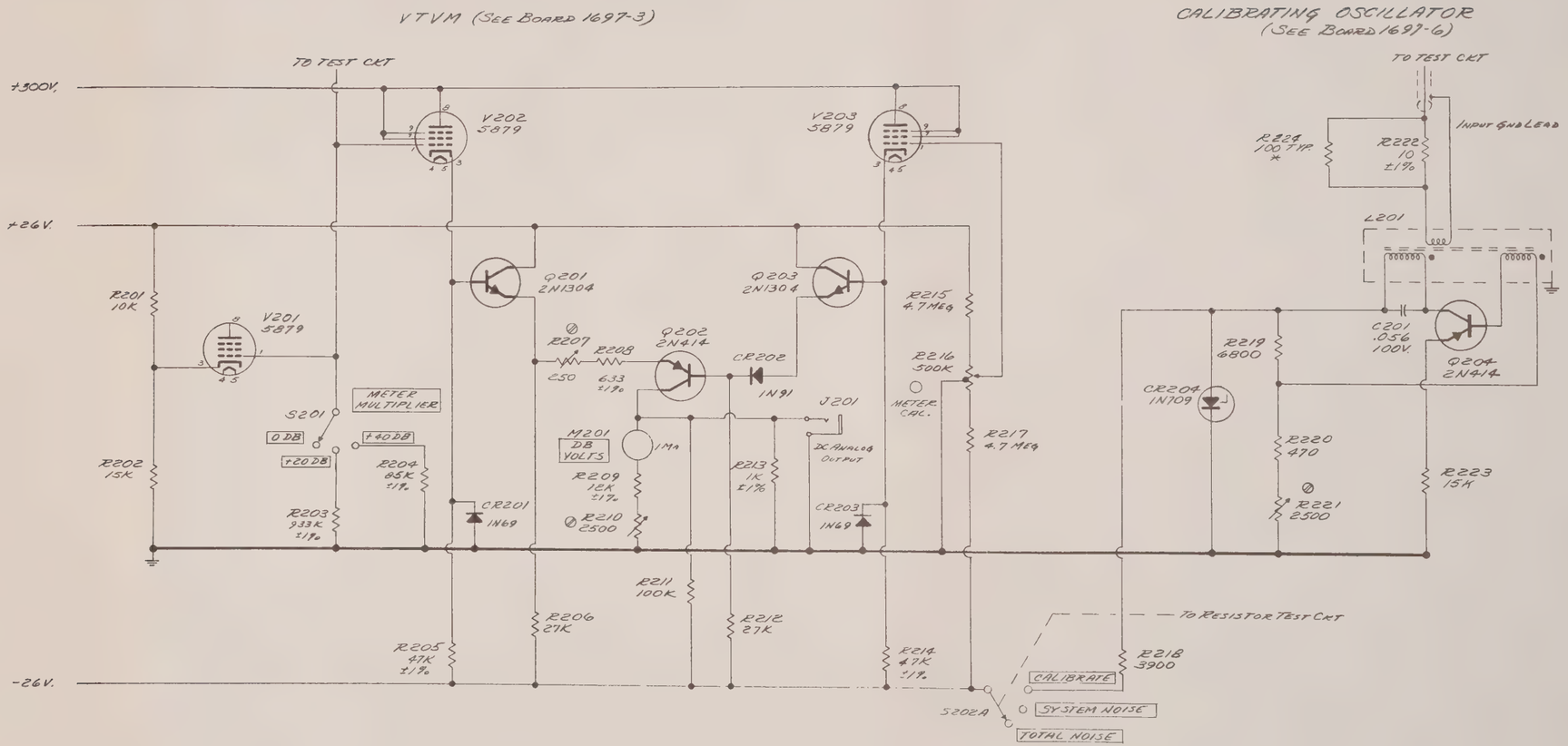
All Resistances in Ohms

All Resistors ½ Watt

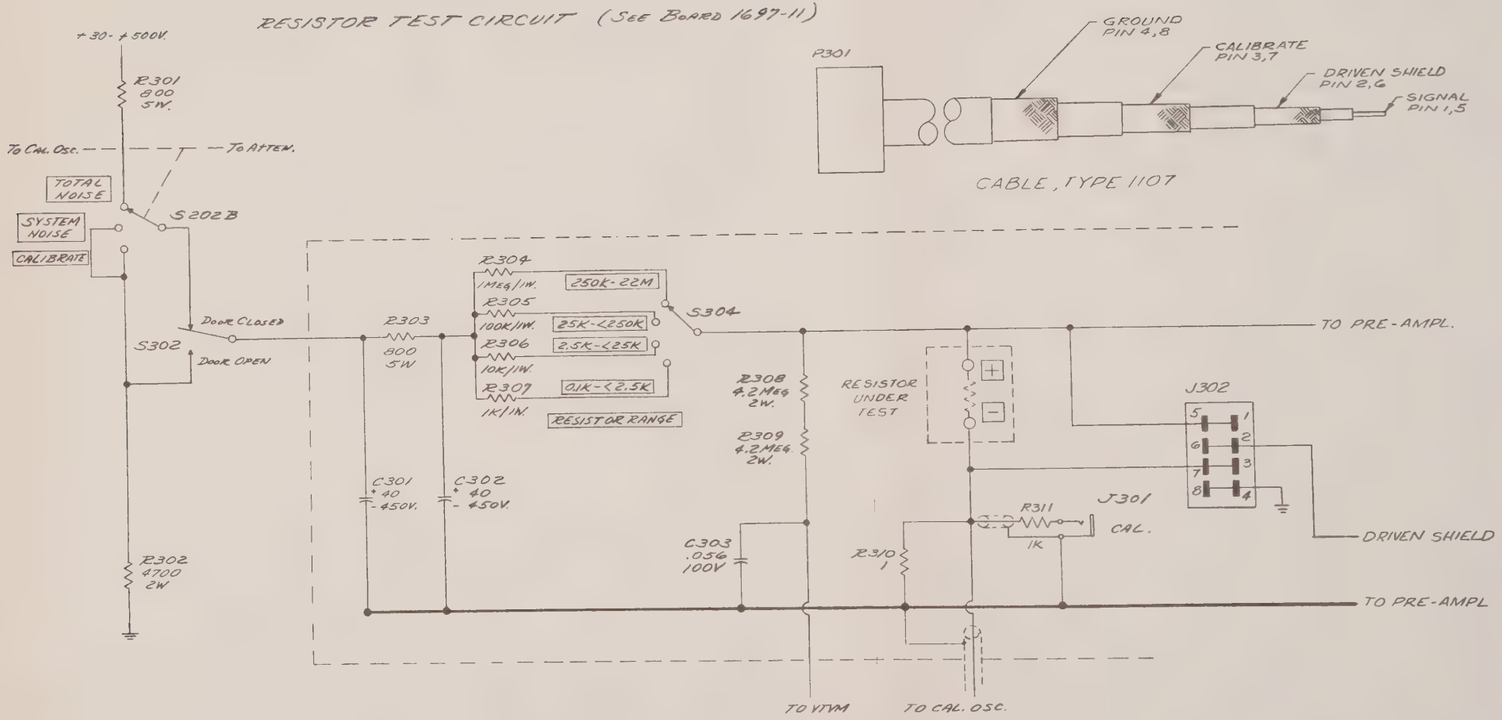
All Capacitances in Microfarads



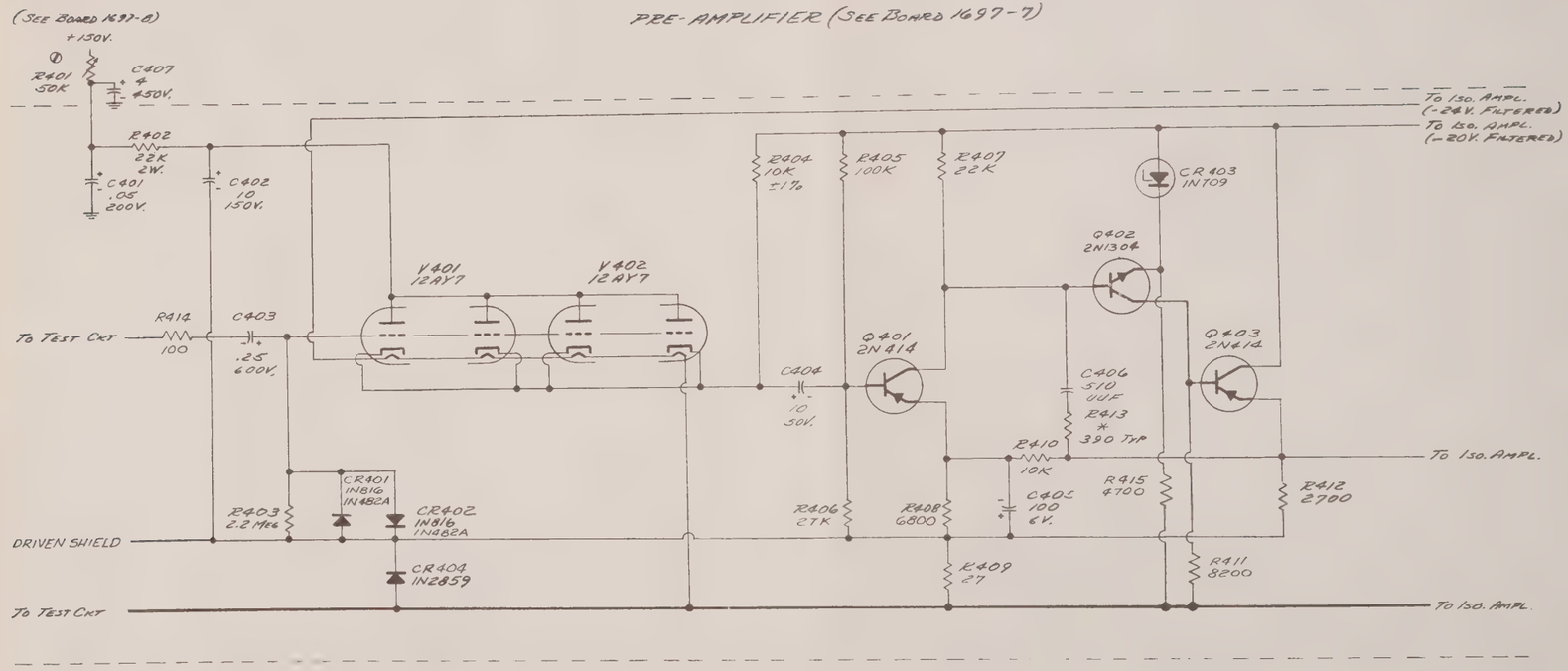
SCHEMATIC
POWER SUPPLY
MODEL 315
(Drawing No. T-1901-L)



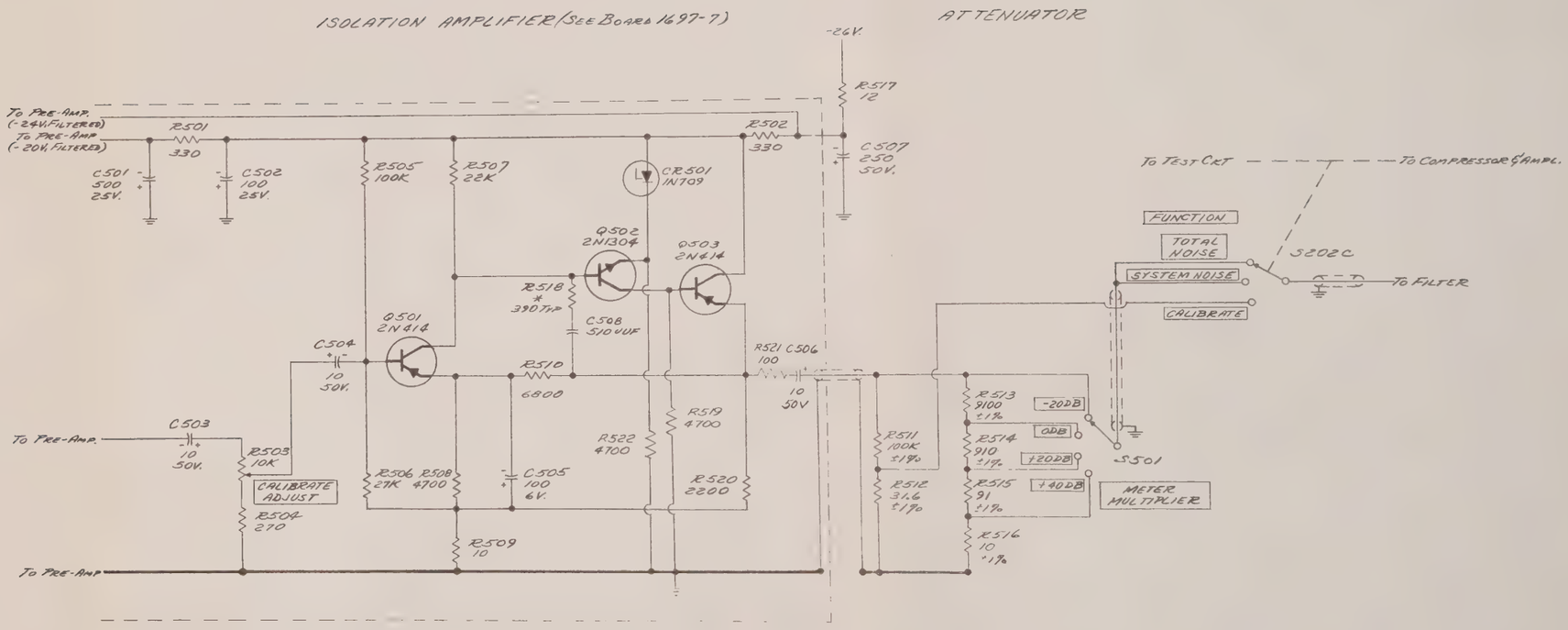
SCHEMATIC
VTVM AND CALIBRATING OSCILLATOR
MODEL 315
(Drawing No. T-1902-D)



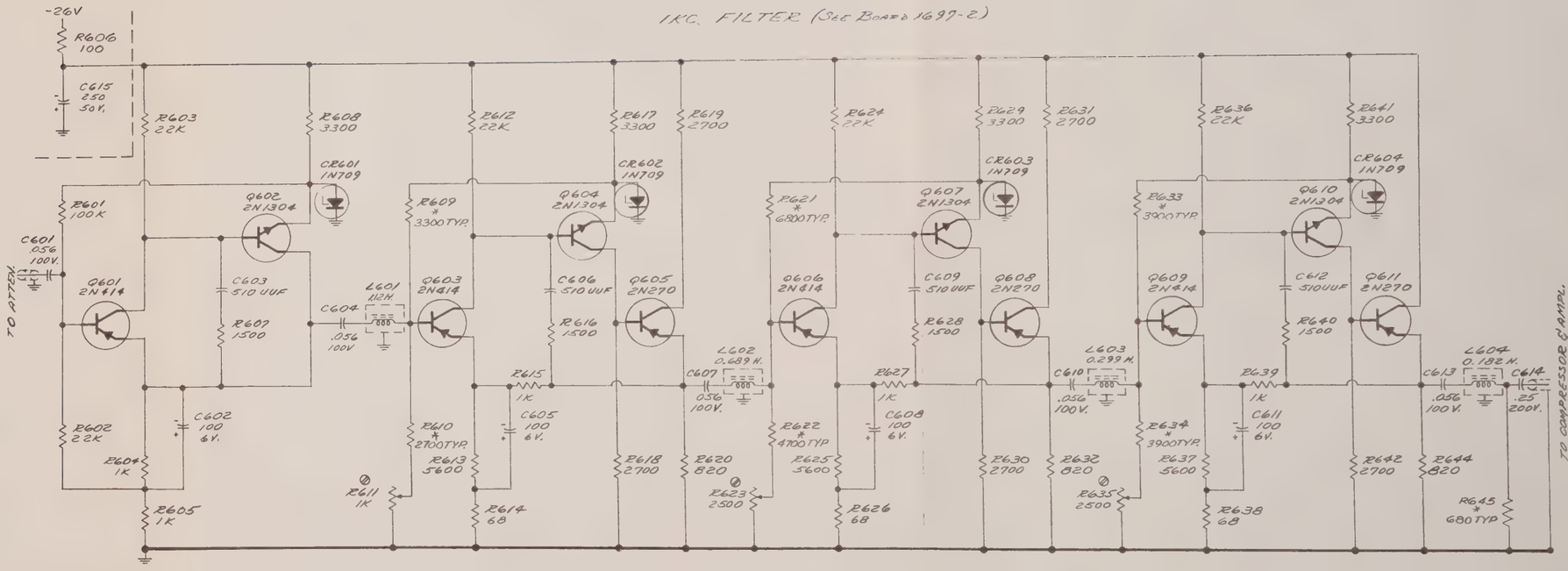
SCHEMATIC
RESISTOR TEST CIRCUIT
MODEL 315
(Drawing No. T-1903-E)



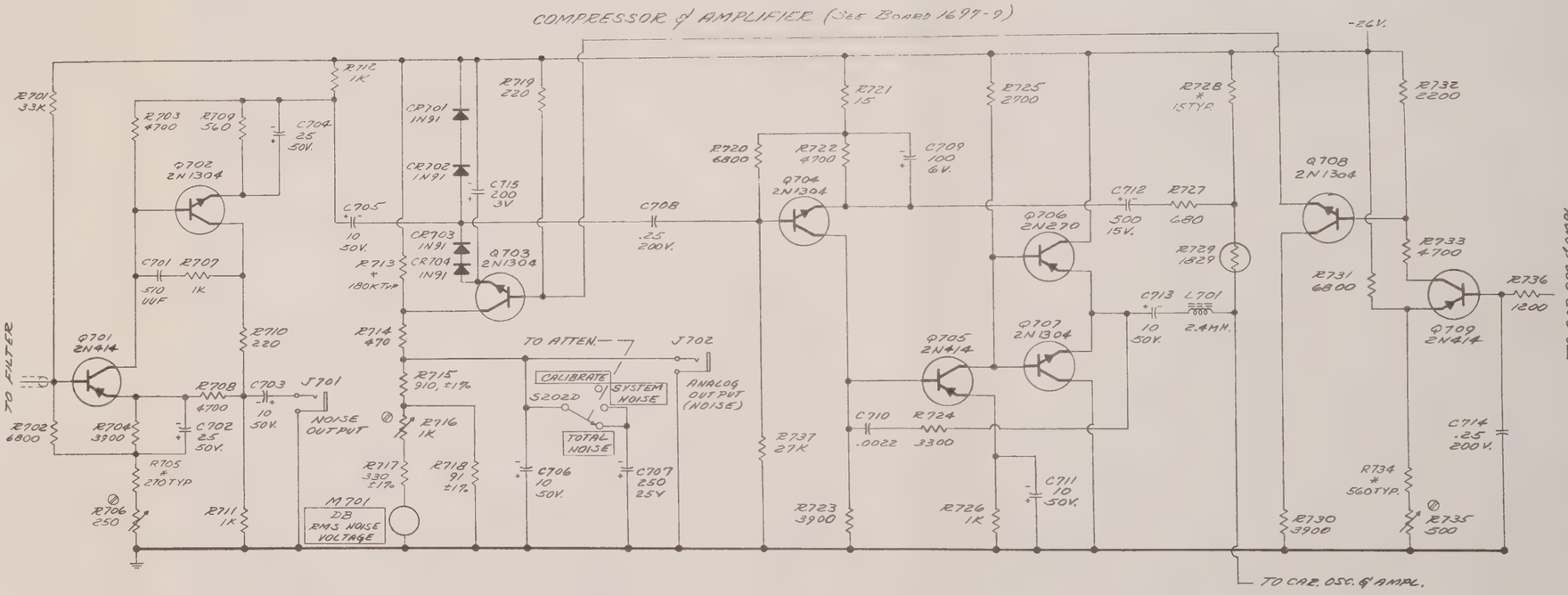
SCHEMATIC
PRE-AMPLIFIER
MODEL 315
(Drawing No. T-1904-J)



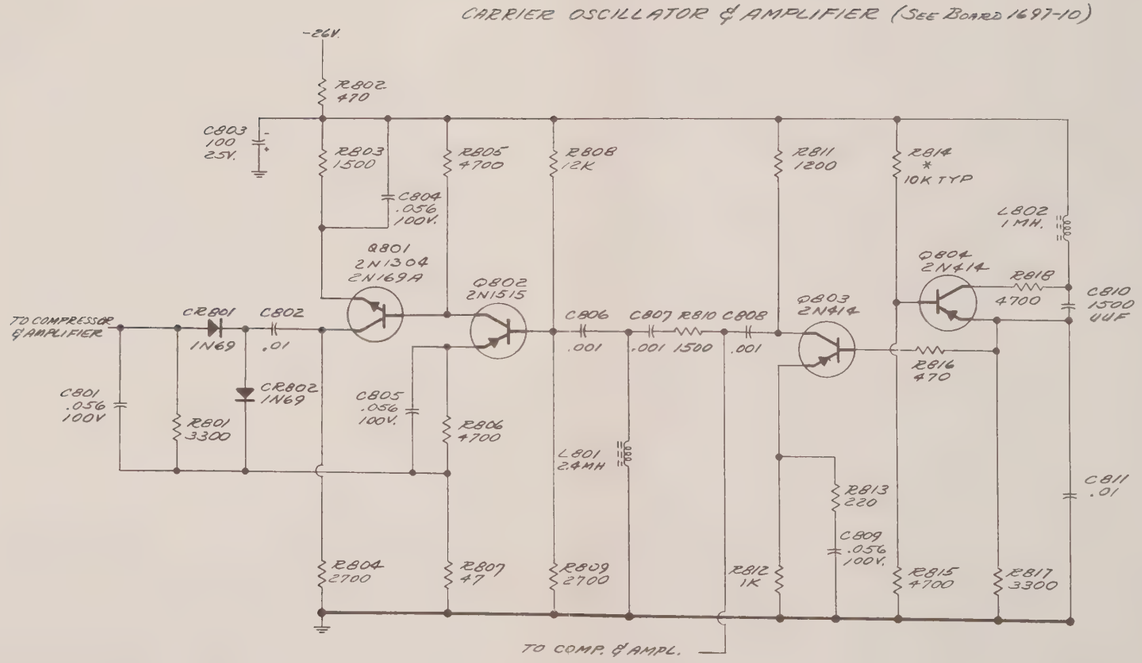
SCHEMATIC
ISOLATION AMPLIFIER AND ATTENUATOR
MODEL 315
(Drawing No. T-1905-G)



SCHEMATIC
FILTER
MODEL 315
(Drawing No. T-1906-H)



SCHEMATIC
COMPRESSOR AND AMPLIFIER
MODEL 315
(Drawing No. T-1907-G)



SCHEMATIC
CARRIER OSCILLATOR AND AMPLIFIER
MODEL 315
(Drawing No. T-1908-C)

METHOD 308

CURRENT-NOISE TEST FOR FIXED RESISTORS

1. PURPOSE. This resistor noise test method is performed for the purpose of establishing the "noisiness" or "noise quality" of a resistor in order to determine its suitability for use in electronic circuits having critical noise requirements. This method is intended as a standard reference for the determination of current noise present in a resistor, for use in an application with specific current-noise requirements. It is not intended as a general specification requirement. Interference caused by the generation of spurious noise signals in parts tends to mask the desired output signal, thus resulting in loss of information. For low-level audiofrequency and other low-frequency circuits, where low-noise parts are used, resistors may become an important source of interfering noise. One source of noise in a resistor is molecular thermal motion which generates a fluctuation voltage termed "thermal noise." It is not necessary to determine the magnitude of thermal noise by measurement since the mean-square value of the fluctuation voltage is predictable from Nyquist's equation, which shows the mean-square value to be proportional to the product of resistance, temperature, and the pass band of the measuring system. Generally, an increase in fluctuation voltage appears when direct current (dc) is passed through resistive circuit elements. The *increase* in fluctuation voltage is termed "excess noise" or "current noise." The magnitude of current noise is dependent upon many inherent properties of the resistor such as resistive material and other factors such as processing, fabrication, size and shape of resistive element, etc. Since there is no apparent functional relationship between current noise and many of these factors, current noise generally cannot be predicted from physical constants. Therefore, it is necessary to measure current noise to determine its magnitude. The method employed in this test has been designed to evaluate accurately the "noisiness" or "noise quality" of individual resistors in terms of a noise-quality index. The noise-quality index, expressed in decibels (db), is a measure of the ratio of the root-mean-square (rms) value of current-noise voltage, in microvolts (uv), to the applied dc voltage, in volts. The pass band associated with the noise-quality index is one frequency decade, geometrically centered at 1,000 cycles per second (cps). This index is termed the "microvolts-per-volt-in-a-decade" index. In the design of circuits, an added advantage accrues from the definitiveness of the index which allows the estimation of interference attributable to current noise. Conversely, for a given limit of current-noise inteference in a particular circuit design, a maximum acceptable value of the index may be established. Ordinarily, it is not necessary to duplicate the operating conditions of the particular circuit design when measuring the current noise. The noise quality of populations of resistors may be reasonably estimated by measurement of the index of representative groups of resistors using suitable sampling procedures. Measurements on sample groups tend to have a normal distribution and once representative parameter values for the distribution have been established (the mean and standard deviation), such parameter values would serve as norms in judging "noisiness" and product uniformity insofar as noise is concerned.

1.1 Precautions. Adherence to the ambient temperature specified in 3.1 is emphasized as an important consideration of this method. It is also necessary, in making noise measurements, using the apparatus of this method, to delay reading the noise meter for a period

of time no less than four times the effective time constant of the detector to allow the meter sufficient time to reach at least 98 percent of a representative average value. The effective time constant of the apparatus is normally adjusted to a value close to 1 second and therefore, a minimum time delay of 4 seconds is normally required for the noise meter to indicate a valid average. Immediately after this 4-second delay, the meter should be read even though it continues to fluctuate as the noise signal varies. Normally, the operator in making a visual reading of the fluctuating meter pointer, should estimate an average for a short duration, in the order of ½ to 1 second.

2. APPARATUS. Noise measurements shall be made on Quan-Tech Laboratories, Inc. Model 315 Resistor-Noise Test Set, or equal, built in conformance with specifications recommended by the National Bureau of Standards (NBS) and detailed in a report entitled "A Recommended Standard Resistor-Noise Test System," by G. T. Conrad, Jr., N. Newman, and A. P. Stansbury published in the IRE Transactions of the Professional Group on Component Parts, Volume CP-7, Number 3, September 1960. The NBS-test system provides a means for establishing direct current through the resistor under test and measuring the resutling dc voltage and noise voltage appearing at the terminals of the resistor. These two voltages are indicated simultaneously on scales calibrated in db. Instrumentation is so arranged that the associated value of the "microvolts-per-volt-in-a-decade" index may be readily determined in accordance with 3.3.

2.1 Test system. The test system shall be as shown in the simplified block diagram in figure 308-1. The dc portion of the system consists of a variable dc power supply and a dc vacuum-tube voltmeter (VTVM). The alternating-current (ac) portion of the system consists of a calibration signal source and an indicating amplifier. The interconnecting leads, as well as the resistor under test, should be adequately shielded.

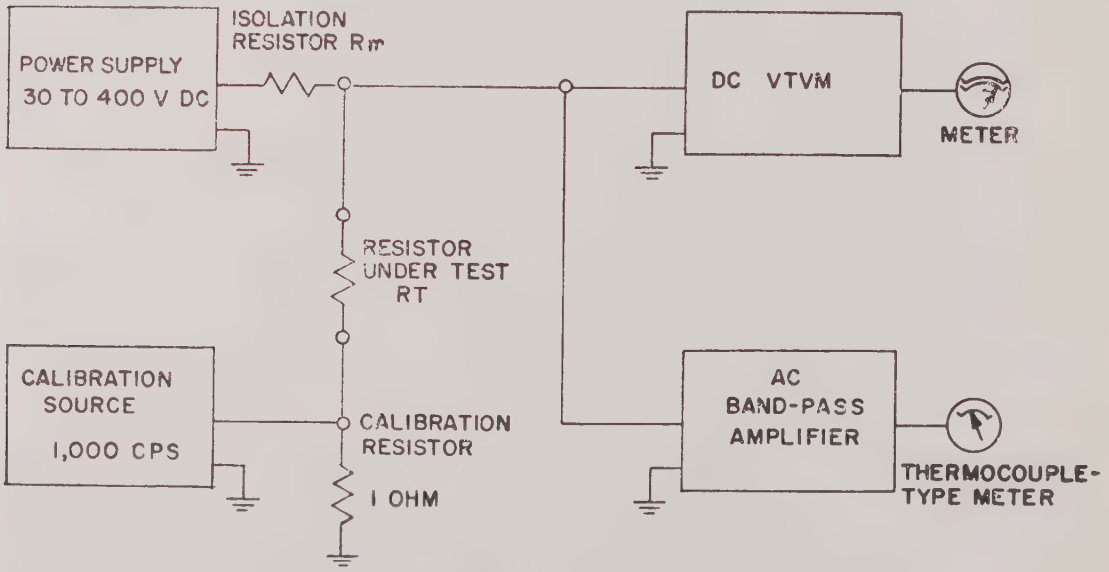


FIGURE 308-1. *Block diagram of system.*

2.1.1 *Dc-measurement considerations.* The variable dc power supply furnishes dc loading power through an isolation resistor to the resistor under test. The isolation resistor prevents noise, appearing at the terminals of the resistor under test, from being severely attenuated by the very low, parallel impedance presented by the output terminals of the dc power supply. The isolation resistor must be free of current noise. Quiet wirewound-type resistors are suitable. One of four values for the isolation resistor, Rm, (1,000 ohms, 10,000 ohms, 100,000 ohms, or 1 megohm (mego)) is selected, depending on the resistance of the resistor under test, RT. The dc voltage appearing across the resistor under test is indicated by the dc VTVM. The meter has two scales—one showing the dc voltage across the resistor under test, V, and the other indicating the quantity D=20 log V, in db. The db scale simplifies computation of the current-noise index. The choice of value of the dc voltage is not critical, however, to avoid subjecting the resistor under test, and the isolation resistor as well, to excessive dc power dissipation or voltage, or both, standard nominal values of dc voltage and values for the isolation resistor are given in table 308–1.

2.1.2 *Ac - measurement considerations.* Noise voltage appearing at the terminals of the resistor under test is amplified and its rms magnitude is shown by the ac indicating amplifier. The indicating amplifier consists of a high-gain, low-noise amplifier, a filter, an rms detector, and an output meter. The filter restricts the frequency response of the amplifier to a flat-top, 1,000-cps pass band, geometrically centered at 1,000 cps. The output-meter scale, like that of the dc VTVM, is calibrated in db to simplify calculations.

2.1.3 *Calibration technique.* The calibration technique consists of first applying a predetermined value of 1,000-cps, sine-wave signal across a 1-ohm resistor located in series with the resistor under test, and then adjusting the gain of the amplifier, by means of a variable attenuator, until the output meter deflects to the "calibrate" line. This procedure standardizes the gain of the system and calibrates the indicating amplifier. It should be noted that since the calibration setting depends upon the impedance at 1,000 cps of the resistor under test, resistors having the same dc resistance may not calibrate alike. The resistance of the calibration resistor (1 ohm) is considered negligible compared to that of any resistor under test (100 ohms to 22 mego); therefore, the effect of the calibration voltage is equivalent to that of the calibration voltage appearing at the terminals of a zero-impedance generator located in series with the resistor under test. The magnitude of the calibration voltage is so chosen that the indicated output is equal to that which would be obtained if the calibration voltage were a noise voltage having an rms value of 1,000 uv in a decade. Such a signal should produce a reading of 60 db when the system is properly calibrated; thus, 0 db means 1 uv in a decade.

2.2 Synopsis. To summarize, this apparatus provides a measure of the rms value of the current-noise voltage generated in the resistor under test and transmitted in a frequency decade. The calibration technique refers the measured noise voltage to the terminals of an essentially zero-impedance noise-voltage generator located in series with the resistor under test. The noise voltage so measured, when corrected for the presence of system noise, is the "open-circuit" current-noise voltage of the resistor under test. Since both the current-noise voltage and dc voltage are expressed in db, the value of the "microvolts-per-volt-in-a-decade" index is obtained by subtracting the dc reading from the corrected noise reading. The corrected noise reading is discussed in 3.3.

3. PROCEDURE

3.1 Operating conditions. The test shall be performed at an ambient temperature of 25°±2° C., unless otherwise specified. The specimen under test shall be stabilized at room ambient temperature prior to test. No special preparations of the specimen are required other than that its leads be clean. Standard operating conditions, based on the resistance value of the specimen to be tested, are given in table 308–1. The values of the isolation resistor, RM, and the dc voltage, V, should be observed, although they are not critical, because the index is reasonably independent of the values of the isolation resistor and the dc voltage over a broad range. Therefore, it is not necessary to obtain the exact value of dc voltage given in table 308–1, rather to set it near the value, and to read carefully and record its value at the time of the measurement. In no case shall the ratings of the resistor under test be exceeded.

3.2 Measurements. After the operating conditions have been established, the measurement operation shall be performed in three steps, as follows:

(1) Calibration (see 3.2.1).

(2) Measurement of system noise (see 3.2.2).

(3) Simultaneous measurement of the dc voltage and the resulting total noise (see 3.2.3).

Generally, the measurements should be made in the order listed. The precautions in 1.1 should be observed.

3.2.1 *Calibration.* The calibration technique (see 2.1.3) standardizes the gain of the ac system for the particular resistor under test. For the noise measurements in steps 2 and 3 which follow, the sum of the ac attenuator setting and the ac meter reading, in db, is a direct indication of the noise present in terms of an "open-circuit' 'rms noise voltage appearing across the terminals of the resistor under test.

TABLE 308–1. *Standard operating conditions*

Resistance		Resistors ½ watt and higher			Resistors ¼, ⅛, and 1/10 watt		
Resistor under test (Rt)	Isolation resistor (Rm)	20 log V (D)	Dc voltage [1] (V)	Dc power dissipation (Pdc)	20 log V (D)	Dc voltage [1] (V)	Dc power dissipation (Pdc)
Ohms	*Ohms*	*db*	*Volts*	*Milliwatts*	*db*	*Volts*	*Milliwatts*
100	1,000	10.1	3.2	100	10.1	3.2	100
120	1,000	11.6	3.8	120	10.9	3.5	100
150	1,000	13.5	4.7	150	11.8	3.9	100
180	1,000	15.1	5.7	180	12.5	4.2	100
220	1,000	16.9	7.0	220	13.4	4.7	100
270	1,000	18.3	8.2	250	14.3	5.2	100
330	1,000	19.2	9.1	250	15.1	5.7	100
390	1,000	19.9	9.9	250	15.8	6.2	100
470	1,000	20.7	10.8	250	16.7	6.9	100
560	1,000	21.4	11.8	250	17.5	7.5	100
680	1,000	22.3	13.0	250	18.3	8.2	100
820	1,000	23.1	14.3	250	19.2	9.1	100
1,000	1,000	24.0	15.8	250	20.0	10.0	100
1,200	1,000	24.8	17.3	250	20.8	11.0	100
1,500	1,000	25.8	19.4	250	21.7	12.2	100
1,800	1,000	26.6	21.2	250	22.5	13.4	100
2,200	1,000	27.4	23.4	250	23.4	14.8	100
2,700	10,000	28.3	26.0	250	24.3	16.4	100
3,300	10,000	29.2	28.7	250	25.2	18.2	100

TABLE 308–1. *Standard operating conditions*—Continued

Resistance		Resistors ½ watt and higher			Resistors ¼, ⅛, and 1/10 watt		
Resistor under (Rt)	Isolation resistor (Rm)	20 log V (D)	Dc voltage [1] (V)	Dc power dissipation (Pdc)	20 log V (D)	Dc voltage [1] (V)	Dc power dissipation (Pdc)
3,900	10,000	29.9	31.2	250	25.9	19.7	100
4,700	10,000	30.8	34.3	250	26.7	21.7	100
5,600	10,000	31.5	37.4	250	27.5	23.7	100
6,800	10,000	32.3	41.2	250	28.3	26.1	100
8,200	10,000	33.2	45.3	250	29.1	28.6	100
10,000	10,000	34.0	50.0	250	30.1	32.0	100
12,000	10,000	34.8	54.8	250	30.9	35.0	100
15,000	10,000	35.8	61.2	250	31.8	39.0	100
18,000	10,000	36.6	67.1	250	32.5	42.0	100
22,000	10,000	37.4	74.2	250	33.4	47.0	100
27,000	0.10 mego	38.3	82.2	250	34.3	52.0	100
33,000	0.10 mego	39.2	90.8	250	35.1	57.0	100
39,000	0.10 mego	40.0	98.7	250	35.8	62.0	100
47,000	0.10 mego	40.7	108	250	36.7	69.0	100
56,000	0.10 mego	41.5	118	250	37.5	75.0	100
68,000	0.10 mego	42.3	130	250	38.3	82.0	100
82,000	0.10 mego	43.1	143	250	39.2	91.0	100
0.10 mego	0.10 mego	44.0	158	250	40.0	100	100
0.12 mego	0.10 mego	44.8	173	250	40.8	110	100
0.15 mego	0.10 mego	45.8	194	250	41.7	122	100
0.18 mego	0.10 mego	46.5	212	250	42.5	134	100
0.22 mego	0.10 mego	47.5	234	250	43.4	148	100
0.27 mego	1.0 mego	38.6	85.0	26.8	38.6	85.0	26.8
0.33 mego	1.0 mego	40.0	99.0	29.7	40.0	99.0	29.7
0.39 mego	1.0 mego	41.0	112	32.2	41.0	112	32.2
0.47 mego	1.0 mego	42.1	127	34.3	42.1	127	34.3
0.56 mego	1.0 mego	43.1	143	36.5	43.1	143	36.5
0.68 mego	1.0 mego	44.2	161	38.1	44.2	161	38.1
0.82 mego	1.0 mego	45.1	180	39.5	45.1	180	39.5
1.0 mego	1.0 mego	46.0	200	40.0	46.0	200	40.0
1.2 mego	1.0 mego	46.8	218	39.6	46.8	218	39.6
1.5 mego	1.0 mego	47.6	240	38.4	47.6	240	38.4
1.8 mego	1.0 mego	48.0	250	34.7	48.0	250	34.7
2.2 mego	1.0 mego	48.0	250	28.4	48.0	250	28.4
2.7 mego	1.0 mego	48.0	250	23.2	48.0	250	23.2
3.3 mego	1.0 mego	48.0	250	18.9	48.0	250	18.9
3.9 mego	1.0 mego	48.0	250	16.0	48.0	250	16.0
4.7 mego	1.0 mego	48.0	250	13.3	48.0	250	13.3
5.6 mego	1.0 mego	48.0	250	11.2	48.0	250	11.2
6.8 mego	1.0 mego	48.0	250	9.2	48.0	250	9.2
8.2 mego	1.0 mego	48.0	250	7.6	48.0	250	7.6
10 mego	1.0 mego	48.0	250	6.2	48.0	250	6.2
12 mego	1.0 mego	48.0	250	5.2	48.0	250	5.2
15 mego	1.0 mego	48.0	250	4.2	48.0	250	4.2
18 mego	1.0 mego	48.0	250	3.5	48.0	250	3.5
22 mego	1.0 mego	48.0	250	2.8	48.0	250	2.8

[1] Dc voltage across the resistor under test for the measurement of total noise.

3.2.2 *System noise (S).* System noise is the background noise present when direct current is not present in the resistor under test. System noise is indicated after turning off the calibration voltage. The algebraic sum of the ac attenuator setting and the ac meter reading gives the magnitude of system noise, S, in db.

3.2.3 *Total noise (T).* Both the dc voltage and the total noise are measured simultaneously. The value of dc voltage is given in table 308–1. The application of excessive dc voltage should be avoided by setting the dc voltage control to its minimum before applying the voltage, and when the voltage is applied, it should be increased to the desired value. The magnitude of the dc voltage is given by the sum, D, of the dc attenuator setting and the dc meter reading, in db. D equals 20 log V, where V is the dc voltage, in volts, applied to the terminals of the resistor under test. The associated noise measurement indicates the total noise present, ie, the quadratic sum of the system noise and the current noise. This total noise is indicated by T, in db.

3.3 **Determination of the "microvolts-per-volt-in-a-decade" index.** The current-noise index to be compared with the required index (see 5) shall be computed from the three measured quantities S, T, and D, in accordance with the following formula.

$$(\text{Index}),\ \text{in db} = T - f(T) - S) - D.$$

Where:

$$f(T - S),\ \text{in db} = -10 \log \left[1 - 10^{-(T-S)/10}\right].$$

The quantity f(T–S) is a correction for the presence of system noise while T is being measured. Values of f(T–S) are given in table 308–2 as a function of T–S. The quantity T–S represents the indicated increase in noise resulting from the presence of direct current. When this increase, T–S, is greater than 15.0 db, then f(T–S) is essentially zero, and T alone is the measure of current noise.

4. **ERRORS.** Accuracy and repeatability of determinations of the current-noise index are influenced by the combined effects of many factors including the following — characteristics of the test set, ambient temperature, inherent fluctuations in current noise, relative magnitude of current noise as compared to system noise, and delay between the application of dc voltage and observation of meter deflection. Therefore, in the interest of a better understanding of the significance of the measurement, a discussion of errors is included. The erro associated with the determination of the index is a function of two independent errors, one a bias-type or constant error, and the other a random-type or variable error. The bias eror is constant for any particular measuring condition. The maximum bias error introduced by the test set should not exceed 0.4 db. A conservative estimate of the bias error introduced by the permissible departure of ambient temperature from 25° C., as stated in 3.1, is at most 0.2 db. The "worst case" bias error for these two factors is the sum of their absolute values, 0.6 db. Although the bias error for any particular measurement is not known, for purposes of this discussion the "worst case" condition is assumed, and 0.6 db will be considered the magnitude of bias error associated with the index. The random error associated with the index is that of the current noise, [T — f(T–S)]. The index will be considered for two cases; the more simple case where the current noise is relatively large, ie, $T - S > 15.0$ db for which $f(T - S) \cong 0$, and therefore current noise is represented by T alone; and the second case where the current noise is not relatively large and is represented by [T—f(T—S)], with f(T—S) being significant. In either case, the probable error of the index is approximately equal to the error component which predominates,

TABLE 308–2. *Correction factor for presence of "system noise"*

T – S db	f(T – S) Correction factor	T – S db	f(T – S) Correction factor
1.0	6.9	5.4	1.4
1.1	6.5	5.5	1.4
1.2	6.2	5.6	1.4
1.3	5.9	5.7	1.3
1.4	5.6	5.8	1.3
1.5	5.3	5.9	1.3
1.6	5.1	6.0	1.2
1.7	4.9	6.1	1.2
1.8	4.7	6.2	1.2
1.9	4.5	6.3	1.1
2.0	4.3	6.4	1.1
2.1	4.1	6.5	
2.2	3.9	to	1.0
2.3	3.8	6.9	
2.4	3.6	7.0	
2.5	3.5	to	0.9
2.6	3.4	7.3	
2.7	3.3	7.4	
2.8	3.2	to	0.8
2.9	3.1	7.9	
3.0	3.0	8.0	
3.1	2.9	to	0.7
3.2	2.8	8.5	
3.3	2.7	8.6	
3.4	2.6	to	0.6
3.5	2.5	9.3	
3.6	2.4	9.4	
3.7	2.4	to	0.5
3.8	2.3	9.9	
3.9	2.2	10.0	
4.0	2.2	to	0.4
4.1	2.1	11.5	
4.2	2.0	11.6	
4.3	2.0	to	0.3
4.4	1.9	12.7	
4.5	1.9	12.8	
4.6	1.8	to	0.2
4.7	1.8	14.5	
4.8	1.7	14.6	
4.9	1.7	to	0.1
5.0	1.6	15.0	
5.1	1.6		
5.2	1.5	>15.0	≤ 0
5.3	1.5		

whether it be bias error or random error. For the first case, the only significant quantity which varies is T, and therefore the random-error component of the index error is equal to the random error associated with the measurement of the total noise, T. The random error of T is evidenced by fluctuations of the meter pointer and tends to have a normal distribution. The magnitude of the probable random error of T cannot be given explicitly because its value is necessarily a function of the resistor under test and must be determined from measurements. The probable random error of T for different resistors may range from values as low as approximately 0.2 db to values as high as several db in resistors having large noise variations. For resistors having a probable random error of T less than 0.6 db, the probable error of the index is approximately equal to the bias error, assuming the bias error is the "worst case," ie, 0.6 db. This means that on the average, one-half of the measurements would have an error no greater than 0.6 db. On the other hand, when the probable random error of T is greater than the bias error, the probable error of the index is equal to that of T. For the second case, the probable random-error component of the index is greater than that of T alone. This follows because the magnitude of current noise is determined from the difference between two measurements, T and S, each of which fluctuates, rather than from T alone. Measurements indicate that the probable random error of S should be in the order of 0.2 db. Assuming that this is the case, the probable random-error component of the index is approximately double that of T for the measurement condition T — S = 3 db, and approximately four times that of T for the condition T — S = 1.5 db. The limit of sensitivity for measuring the current-noise index is approached as the current noise approaches values to small to cause an increase as much as 1.0 db, ie, T–S equal to 1.0 db. However, the test method may serve as a qualitative means for comparing resistors having relatively low values of current noise where T — S is less than 1.0 db. Another possible

source of measurement uncertainty is the transitory variations in current noise which may immediately follow application of dc voltage. Certain types of resistors tend to display very little, if any, transitory variations, whereas other types tend to display such variations to a measureable degree. For those resistors which exhibit such variations, the current noise usually settles to a more stable value after a short time, from 1 to several seconds. In some cases, the current-noise variations may continue to be relatively large and unstable for extended periods of time. Such resistors are usually very noisy. By adhering to the precautions regarding the procedures stated in 1.1, the effects of such variations on repeated measurements are reduced.

5. **SUMMARY.** The following requirement and details must be provided when this method is specified.

(a) Required values of the "microvolts-per-volt-in-a-decade" index (see 3.3).

(b) Ambient temperature, if other than that specified (see 3.1).

(c) Value of dc voltage, if other than those stated in table 308–1 (see 2.1.1 and 3.1).

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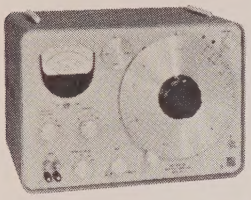
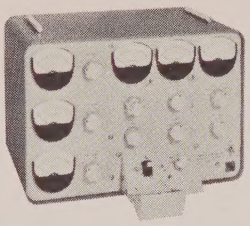
Quan-Tech INSTRUMENTS



MODEL 303
WAVE AND NOISE SPECTRUM ANALYZER

Fully transistorized spectrum analyzer covers frequency range from 30 cps to 100 kc. Front-panel selection of 4 constant bandwidths (10, 30, 100 & 1000 cps) the 100 & 1000 cps bandwidths are flat topped, simplifying noise computations, greatly improving accuracy, and simplifying tuning. Sensitivity: 100 μv to 300 v, full scale; down to 1 μv full scale with Model 203 Amplifier (see below). Additional features: $\pm$ 300 cps vernier; selection of long or short meter time constants; metering circuits compensated to minimize error from instantaneous noise pulses; overload protected meter; analog output for external monitoring.

PRICE: $1425



MODEL 310
TRANSISTOR NOISE ANALYZER

Measures noise at 100 cps, 1 kc and 10 kc simultaneously for 3-point spectrum analysis, allowing identification of 1/f-portion of transistor noise. Measures noise voltage over range from 0.01 to 3 μv/root cycle FS, and noise current from 1 to 300 pa/root cycle, FS. Collector current range, 0.05 to 30 ma; collector voltage range, 0.1 to 30 v. Measuring system automatically corrects for variations in transistor gain; measurement also provided of beta, I_{cbo} and I_{ebo}.

PRICE: $2075

MODEL 311 TRANSISTOR NOISE ANALYZER

Similar to above, except that collector current range extends from 5 to 1000 μamperes, for measurement of noise in low-collector-current devices. Beta measurement is not available in the Model 311.

PRICE: $2275

MODEL 315
RESISTOR NOISE TEST SET

Measures noise in resistors in conformance with specifications recommended by National Bureau of Standards and Method 308 of MIL STD 202 B. Tests resistors from 100 ohms to 22 megohms. Range of measurement: 0.6 μv in a decade to 1000 μv in a decade. Output of noise voltage for external monitoring; analog outputs of meter readings for data logging, etc. External cable included to permit locating test jig up to 10-feet from instrument.

PRICE: $1700

MODEL 2136

Same specifications as Model 315 except measures resistors down to 10 ohms.

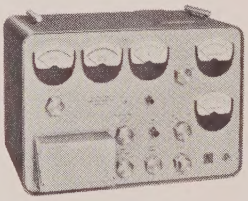
PRICE: $2300

MODEL 317
AMPLITUDE DISTRIBUTION ANALYZER

Establishes the amplitude-probability distribution of random signals to determine whether distribution is Gaussian, or to establish threshold requirements, false-alarm probabilities, etc. Amplifier response: 3db down at approx. 12 cps and 1 mc. Switching rate: 5 mc. Amplitude ranges: 100%, 10% and 1%, FS. "inverted" operation, indicating what percentage of time preset limit is not exceeded, also provided. Output to drive counter at front panel; voltage level may be swept from external source (such as oscilloscope sweep output) for automatic display.

PRICE: $395

MODEL 327
DIODE NOISE ANALYZER



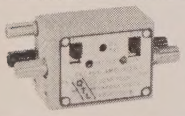
Measures noise in back-biased semi-conductor diodes over range of 0.03 μv to 1 mv per cycle of bandwidth at 10 cps and 1 kc simultaneously. Diode test voltage adjustable up to 500 v; current, to 100 ma. Internally generated ramp sweeps test voltage and/or current automatically within maximum ratings. Sweep selectable in 3 speeds. A wide variety of signal and analog outputs for data logging, external monitoring, actuating external equipment, etc.

PRICE: $2450

MODEL 420 RANDOM NOISE GENERATOR

Provides stable "white" noise output that is gaussian in amplitude distribution from DC to 100 KC. Calibrated output is continuously variable from 0.01 to 1000 μv per root cycle. DC offset is less than 10 mv at max. output. Completely solid-state instrument measures 12" x 6" x 8". **PRICE: $525**

SOLID STATE AMPLIFIERS



MODEL 201-B
DC-COUPLED DECADE AMPLIFIER

Provides controlled gain of 10 from DC to 3 mc (3db). Completely self-contained; battery operated; built-in battery-condition indicator.

PRICE: $95

MODEL 203
LOW NOISE AC AMPLIFIER

Controlled gain of 100 from 30 cps to 100 kc ($\pm$0.5 db), down 3 db at 500 kc. Typical noise: 5 x 10^{-9}V and 3 x 10^{-12}A per root cycle at 1 kc. Two Mod. 203's may be plugged together in series for gain of 10,000. Battery operated; fully self-contained; built-in battery condition indicator.

PRICE: $125

MODEL 205
HIGH-STABILITY DC AMPLIFIER

Controlled gain of 10 from dc to 100 kc. Highly stable: typical shorted input drift less than 250 μv at room ambient. Octal basing for plug-in installation. External + and — 12 v. required.

PRICE: $105

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